

# UCC25600 8-Pin High-Performance Resonant Mode Controller

## 1 Features

- Variable switching frequency control
- Programmable minimum switching frequency with 4% accuracy (3% accuracy at temperature range:  $-20^{\circ}\text{C}$  to  $105^{\circ}\text{C}$ )
- Programmable maximum switching frequency
- Programmable dead time for best efficiency
- Programmable soft-start time
- Easy ON and OFF control
- Overcurrent protection
- Overtemperature protection
- Bias voltage UVLO and overvoltage protection
- Integrated gate driver with 0.4-A source and 0.8-A sink capability
- Operating temperature range:  $-40^{\circ}\text{C}$  to  $125^{\circ}\text{C}$
- SOIC 8-Pin package

## 2 Applications

- 100W to 1kW power supplies
- LCD, Plasma, and DLP® TVs
- Adaptors, computing, and ATX power supplies
- Home audio systems
- Electronic lighting ballasts

## 3 Description

The UCC25600 high performance, resonant mode controller is designed for dc-to-dc applications using resonant topologies, especially the LLC half-bridge resonant converter. This highly integrated controller implements frequency modulation control and complete system functions in only an 8-pin package. Switching to the UCC25600 will greatly simplify the system design and layout, and improve time to market, all at a price point lower than competitive 16-pin device offerings.

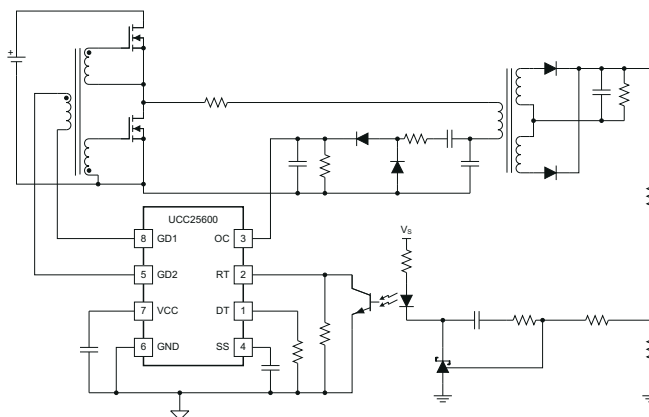
The internal oscillator supports the switching frequencies from 40 kHz to 350 kHz. This high-accuracy oscillator realizes the minimum switching frequency limiting with 4% tolerance, allowing the designer to avoid over-design of the power stage and, thus, further reducing overall system cost. The programmable dead time enables zero-voltage switching with minimum magnetizing current. This maximizes system efficiency across a variety of applications. The programmable soft-start timer maximizes design flexibility demanded by the varied requirements of end equipment using a half-bridge topology. By incorporating a 0.4-A source and 0.8-A sink driving capability, a low cost, reliable gate driver transformer is a real option.

The UCC25600 delivers complete system protection functions including overcurrent, UVLO, bias supply OVP, and overtemperature protection.

### Device Information (1)

PART NUMBER	PACKAGE	BODY SIZE (NOM)
UCC25600	SOIC (8)	3.91 mm × 4.90 mm

- (1) For all available packages, see the orderable addendum at the end of the data sheet.



Typical Application Diagram



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## 4 Revision History

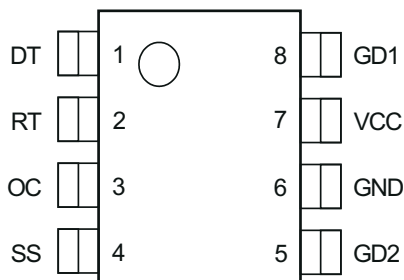
NOTE: Page numbers for previous revisions may differ from page numbers in the current version.

<b>Changes from Revision C (July 2015) to Revision D (August 2024)</b>	<b>Page</b>
• Updated the numbering format for tables, figures, and cross-references throughout the document.....	<b>1</b>

<b>Changes from Revision B (June 2011) to Revision C (July 2015)</b>	<b>Page</b>
• Added <i>ESD Ratings</i> table, <i>Feature Description</i> section, <i>Device Functional Modes</i> , <i>Application and Implementation</i> section, <i>Power Supply Recommendations</i> section, <i>Layout</i> section, <i>Device and Documentation Support</i> section, and <i>Mechanical, Packaging, and Orderable Information</i> section. ....	<b>1</b>

<b>Changes from Revision A (September 2008) to Revision B (June 2011)</b>	<b>Page</b>
• Changed Operating Temperature Range to match the Electrical Specifications.....	<b>1</b>

## 5 Pin Configuration and Functions



**Figure 5-1. D Package 8-Pin SOIC Top View**

**Table 5-1. Pin Functions**

PIN		I/O	DESCRIPTION
NAME	NO.		
DT	1	I	This pin sets the dead time of high-side and low-side switch driving signals. Connect a resistor to ground. With internal 2.25-V voltage reference, the current flowing through the resistor sets the dead time. To prevent shoot through when this pin is accidentally shorted to ground, the minimum dead time is set to 120 ns. Any dead time setting less than 120 ns will automatically have 120-ns dead time.
GD1	8	O	High-side and low-side switch gate driver. Connect gate driver transformer primary side to these two pins to drive the half-bridge.
GD2	5		
GND	6	—	Ground
OC	3	I	Overcurrent protection pin. When the voltage on this pin is above 1 V, gate driver signals are actively pulled low. After the voltage falls below 0.6 V, the gate driver signal recovers with soft-start. When OC pin voltage is above 2 V, the device is latched off. Bringing VCC below the UVLO level resets the overcurrent latch to off.
RT	2	I	The current flowing out of this pin sets the frequency of the gate driver signals. Connect the opto-coupler collector to this pin to control the switching frequency for regulation purposes. Parallel a resistor to ground to set the minimum current flowing out of the pin and set the minimum switching frequency. To set the maximum switching frequency limiting, simply series a resistor with the opto-coupler transistor. This resistor sets the maximum current flowing out of the pin and limits the maximum switching frequency.
SS	4	I	Soft-start pin. This pin sets the soft-start time of the system. Connect a capacitor to ground. Pulling this pin below 1 V will disable the device to allow easy ON/OFF control. The soft-start function is enabled after all fault conditions, including bias supply OV, UVLO, overcurrent protection, and overtemperature protection.
VCC	7	—	Bias Supply. Connect this pin to a power supply less than 20 V. Parallel a 1-μF capacitor to ground to filter out noise.

## 6 Specifications

### 6.1 Absolute Maximum Ratings

over operating free-air temperature range (unless otherwise noted) <sup>(1)</sup>

	MIN	MAX	UNIT
Supply voltage, VCC		22	V
Voltage, GD1, GD2	−0.5	VCC + 0.5	V
Gate drive current – continuous, GD1, GD2		±25	mA
Current, RT		−5	mA
Current, DT		−0.7	mA
Lead temperature (10 seconds)		260	°C
Operating junction temperature, T <sub>J</sub>	−40	125	°C
Storage temperature, T <sub>stg</sub>	−65	150	°C

- (1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only, which do not imply functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Conditions*. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.

### 6.2 ESD Ratings

		VALUE	UNIT
V <sub>(ESD)</sub> Electrostatic discharge	Human body model (HBM), per ANSI/ESDA/JEDEC JS-001, all pins <sup>(1)</sup>	±2000	V
	Charged device model (CDM), per JEDEC specification JESD22-C101, all pins <sup>(2)</sup>	±500	

- (1) JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process.  
 (2) JEDEC document JEP157 states that 250-V CDM allows safe manufacturing with a standard ESD control process.

### 6.3 Recommended Operating Conditions

over operating free-air temperature range (unless otherwise noted)

	MIN	NOM	MAX	UNIT
VCC input voltage from a low-impedance source	11.5		18.0	V
RT resistance	1		8.666	kΩ
DT resistance	3.3		39	kΩ
SS capacitor	0.01		1	μF

### 6.4 Thermal Information

THERMAL METRIC <sup>(1)</sup>		UCC25600	UNIT
		D (SOIC)	
		8 PINS	
R <sub>θJA</sub>	Junction-to-ambient thermal resistance	118.5	°C/W
R <sub>θJC(top)</sub>	Junction-to-case (top) thermal resistance	72.5	°C/W
R <sub>θJB</sub>	Junction-to-board thermal resistance	58.9	°C/W
Ψ <sub>JT</sub>	Junction-to-top characterization parameter	24.1	°C/W
Ψ <sub>JB</sub>	Junction-to-board characterization parameter	58.4	°C/W

- (1) For more information about traditional and new thermal metrics, see the *Semiconductor and IC Package Thermal Metrics* application report, [SPRA953](#).

## 6.5 Electrical Characteristics

over operating free-air temperature range (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
BIAS SUPPLY (VCC)						
VCC current, disabled		SS = 0 V		1	1.5	mA
VCC current, enabled		SS = 5 V, C <sub>GD1</sub> = C <sub>GD2</sub> = 1 nF	2.5	5	7.5	mA
VCC current, UVLO		VCC = 9 V		100	400	μA
V <sub>UVLO</sub>	UVLO turn-on threshold	Measured at VCC rising	9.9	10.5	11.1	V
	UVLO turn-off threshold	Measured at VCC falling	8.9	9.5	10.1	V
	UVLO hysteresis	Measured at VCC	0.7	1	1.3	V
V <sub>OVP</sub>	OVP turn-off threshold	Measured at VCC rising	18	20	22	V
	OVP turn-on threshold	Measured at VCC falling	16	18	20	V
	OVP hysteresis	Measured at VCC	1.5	2	2.5	V
DEAD TIME (DT)						
T <sub>DT</sub>	Dead time	R <sub>DT</sub> = 16.9 kΩ	390	420	450	ns
OSCILLATOR						
F <sub>SW(min)</sub>	Minimum switching frequency at GD1, GD2	–40°C to 125°C	40.04	41.70	43.36	kHz
		–20°C to 105°C	40.45	41.70	42.95	
K <sub>ICO</sub>	Switching frequency gain/I (RT)	R <sub>RT</sub> = 4.7 kΩ, I <sub>RT</sub> = 0 to 1 mA	60	80	100	Hz/μA
GD1, GD2 on time mismatching			–50		50	ns
F <sub>SW_BM</sub>	Switching frequency starting burst mode	SS = 5 V	300	350	400	kHz
	Switching frequency to come out of burst mode	SS = 5 V	280	330	380	kHz
F <sub>SW(start)</sub>	Switching frequency at soft-start	–40°C to 125°C	122	142.5	162	kHz
		–20°C to 105°C	125	142.5	160	
EXTERNAL DISABLE/SOFT START						
Enable threshold		Measure at SS rising	1.1	1.2	1.3	V
Disable threshold		Measured at SS falling	0.85	1	1.1	V
Disable hysteresis		Measured at SS	0.15		0.35	V
Disable prop. delay		Measured between SS (falling) and GD2 (falling)	250	500	750	ns
I <sub>SS</sub>	Source current on ISS pin	V <sub>SS</sub> = 0.5 V	–225	–175	–125	μA
		V <sub>SS</sub> = 1.35 V	–5.5	–5	–4.5	
PEAK CURRENT LIMIT						
V <sub>OC1(off)</sub>	Level 1 overcurrent threshold – V <sub>OC</sub> rising		0.9	1	1.1	V
V <sub>OC2(off)</sub>	Level 2 overcurrent latch threshold – V <sub>OC</sub> rising		1.8	2.0	2.2	V
V <sub>OC1(on)</sub>	Level 1 overcurrent threshold – V <sub>OC</sub> falling		0.5	0.6	0.7	V
T <sub>d_OC</sub>	Propagation delay		60	200	500	ns
I <sub>OC</sub>	OC bias current	V <sub>OC</sub> = 0.8 V	–200		200	nA

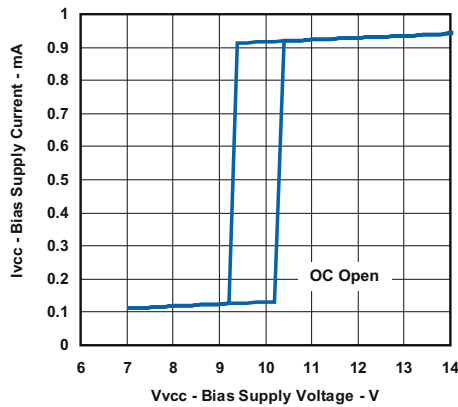
## 6.5 Electrical Characteristics (continued)

over operating free-air temperature range (unless otherwise noted)

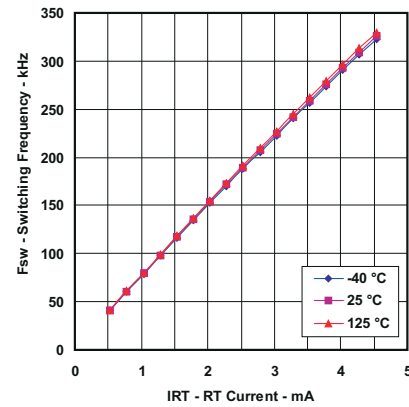
PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
<b>GATE DRIVE</b>					
GD1, GD2 output voltage high	$I_{GD1}, I_{GD2} = -20 \text{ mA}$	9		11	V
GD1, GD2 on resistance high	$I_{GD1}, I_{GD2} = -20 \text{ mA}$		12	30	$\Omega$
GD1, GD2 output voltage low	$I_{GD1}, I_{GD2} = 20 \text{ mA}$		0.08	0.2	V
GD1, GD2 on resistance low	$I_{GD1}, I_{GD2} = 20 \text{ mA}$		4	10	$\Omega$
Rise time GDx	1 V to 9 V, $C_{LOAD} = 1 \text{ nF}$		18	35	ns
Fall time GDx	9 V to 1 V, $C_{LOAD} = 1 \text{ nF}$		12	25	
GD1, GD2 output voltage during UVLO	$V_{CC} = 6 \text{ V}, I_{GD1}, I_{GD2} = 1.2 \text{ mA}$	0.5		1.75	V
<b>THERMAL SHUTDOWN</b>					
Thermal shutdown threshold			160		$^{\circ}\text{C}$
Thermal shutdown recovery threshold			140		$^{\circ}\text{C}$

## 6.6 Typical Characteristics

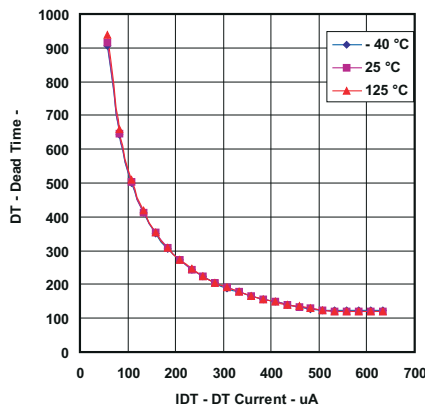
At  $V_{CC} = 12\text{ V}$ ,  $R_{RT} = 4.7\text{ k}\Omega$ ,  $R_{DT} = 16.9\text{ k}\Omega$ ,  $V_{SS} = 5\text{ V}$ ,  $V_{OC} = 0\text{ V}$ ; all voltages are with respect to GND,  $T_J = T_A = 25^\circ\text{C}$ , unless otherwise noted.



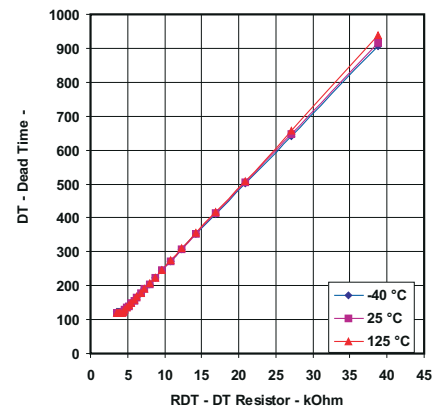
**Figure 6-1. Bias Supply Current vs Bias Supply Voltage**



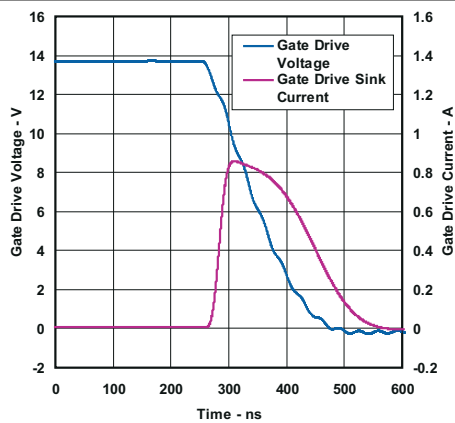
**Figure 6-2. Switching Frequency vs RT Current**



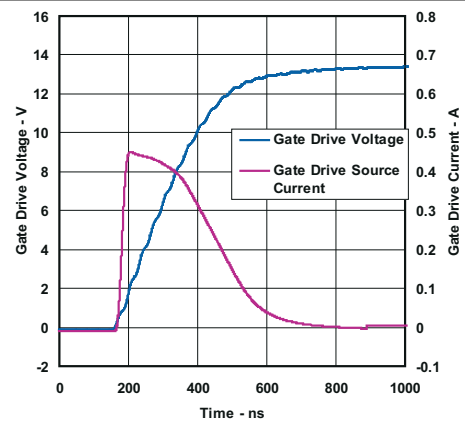
**Figure 6-3. Dead Time vs DT Current**



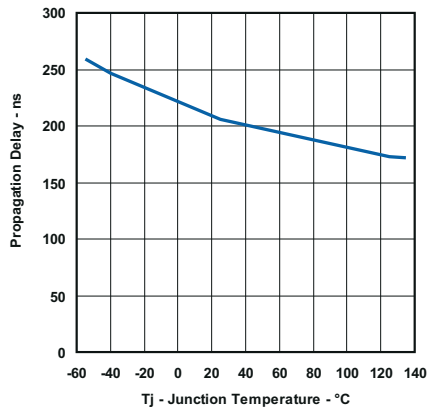
**Figure 6-4. Dead Time vs DT Resistor**



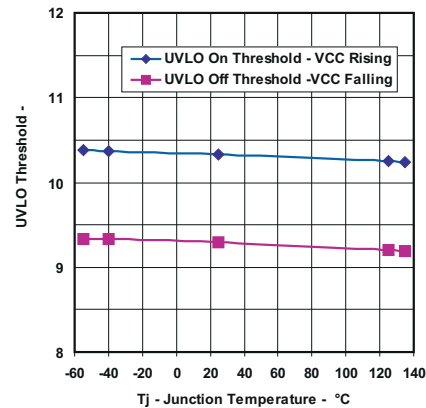
**Figure 6-5. Gate Drive Falling, VCC = 15 V**



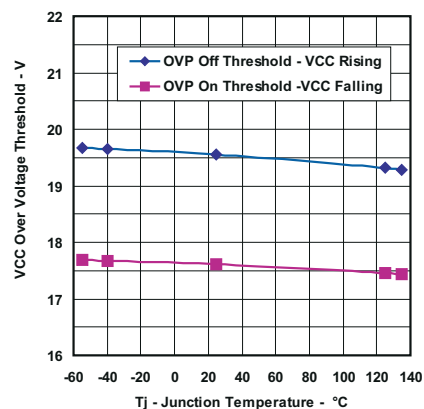
**Figure 6-6. Gate Drive Rising, VCC = 15 V**



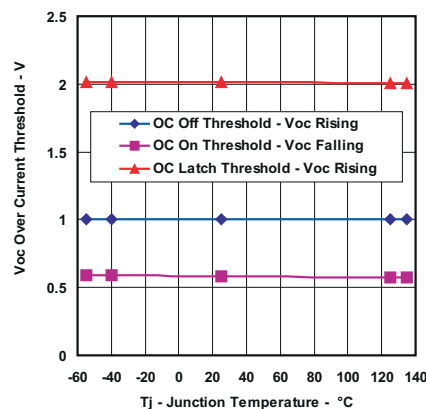
**Figure 6-7. Overcurrent Propagation Delay vs Temperature**



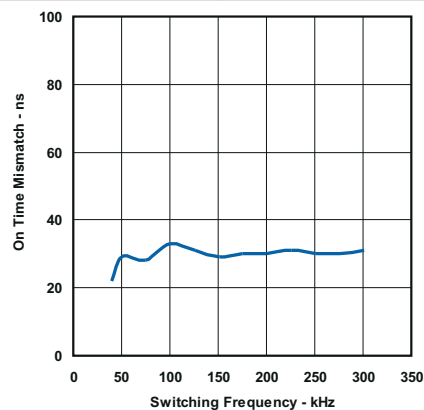
**Figure 6-8. UVLO Threshold vs Temperature**



**Figure 6-9. VCC Overvoltage Threshold vs Temperature**



**Figure 6-10. Overcurrent Threshold vs Temperature**



**Figure 6-11. On-time Mismatch vs Switching Frequency**



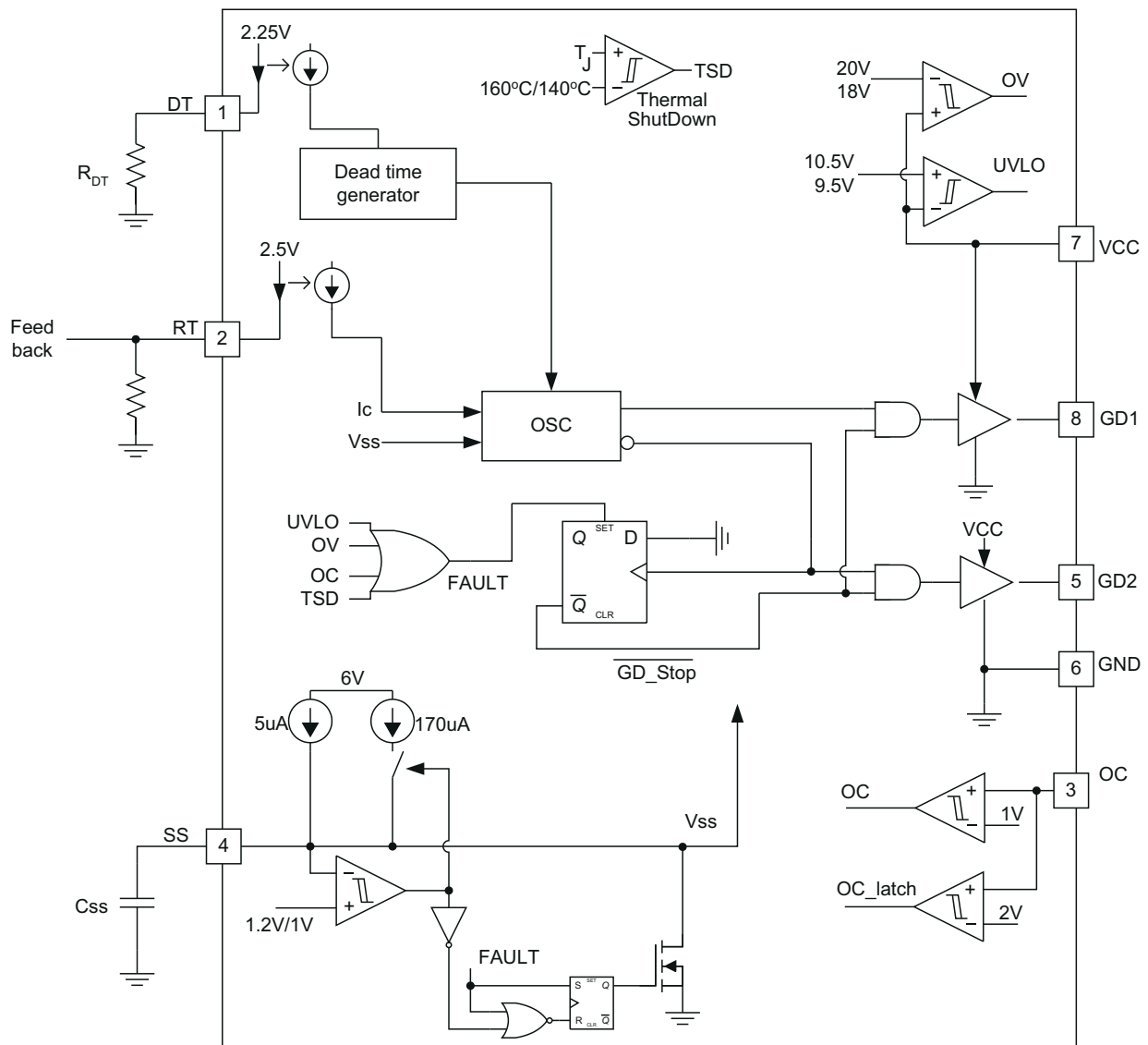
## 7 Detailed Description

### 7.1 Overview

Due to high power density and high efficiency requirements, LLC topology is employed in many applications. The LLC resonant converter has many unique characteristics and improvements compared with hard-switch bridge topology and phase-shift full bridge. For example, LLC has a simple structure, and could achieve primary MOSFET zero voltage switching (ZVS) and the secondary rectifier zero current switching (ZCS) from no load to full load.

The UCC25600 device is an LLC-resonant half-bridge controller which integrates built-in, state-of-the-art efficiency boost features with high-level protection features to provide cost-effective solutions.

### 7.2 Functional Block Diagram

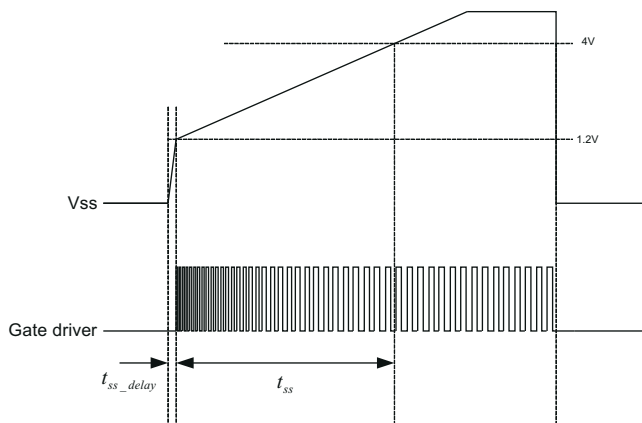


## 7.3 Feature Description

### 7.3.1 Soft Start

During start-up and fault recovery conditions, soft start is always implemented to prevent excessive resonant tank current and to ensure zero-voltage switching (ZVS). During soft start, the switching frequency is increased. The soft-start time can be programmed by placing a capacitor from the SS pin to ground.

The soft-start pin also serves as an ON/OFF control pin of the device. By actively pulling the SS pin below 1 V, the device is disabled. When the pulldown is removed, SS pin voltage is increased because of internal charging current. Once the SS pin is above 1.2 V, the device starts to generate a gate-driver signal and enters soft-start mode. The time sequence of soft start is shown in Figure 7-1.



**Figure 7-1. Soft-Start Sequence**

To prevent a long delay between the ON command and appearance of a gate driver signal, the SS pin current is set as two different levels. When the SS pin voltage is below 1.2 V, its output current is 175  $\mu$ A. This high current could charge the soft-start pin capacitor to 1.2 V in a short period of time, and reduce the time delay. This time delay can be calculated using following equation:

$$t_{SS\_delay} = \frac{1.2V}{175\mu A} C_{SS} \quad (1)$$

The switching frequency during soft start is determined by both the current flowing out of the RT pin and the voltage on the SS pin. The switching frequency can be calculated based on the following equation:

$$f_s = \frac{1}{2} \frac{1}{\frac{6ns \times 1A}{I_{RT} + \left(1.81mA - \frac{V_{SS}}{2.2k\Omega}\right)} + 150ns} \quad (2)$$

After the SS pin voltage reaches 4 V, the soft-start period is finished and switching frequency becomes the same as demanded by the RT pin current. The time used to charge the SS pin from 1.2 V to 4 V is defined as soft-start time and can be calculated as:

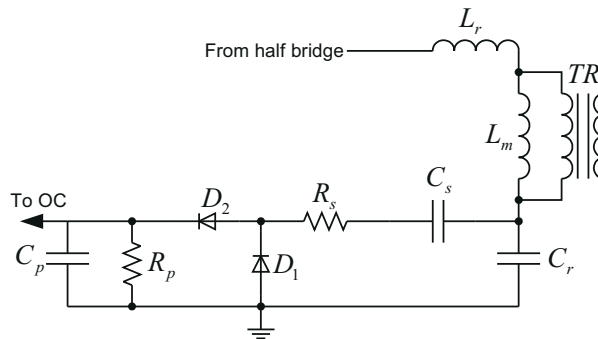
$$t_{ss} = \frac{2.8V}{5\mu A} C_{ss} \quad (3)$$

To ensure reliable operation, the gate drivers restart with GD2 turning high. This prevents uncertainty during system start up.

### 7.3.2 Overcurrent Protection

To prevent power stage failure under excessive load current condition, the UCC25600 includes an overcurrent protection function. With a dedicated OC pin, the power stage is shut down when OC pin voltage is above 1 V. Once the OC pin voltage becomes lower than 0.6 V, the gate driver recovers with a soft start. To enhance system safety, the UCC25600 latches up the whole system when the OC pin becomes above 2 V. Bring VCC below the UVLO level to reset the device.

The current can be indirectly sensed through the voltage across the resonant capacitor by using the sensing network shown in Figure 7-2.



**Figure 7-2. Current Sensing for LLC Resonant Converter**

The general concept of this sensing method is that the ac voltage across the resonant capacitor is proportional to load current.

According to the FHA model, peak voltage of the ac component on the resonant capacitor can be calculated as:

$$V_{Cr\_pk} = \frac{4}{\pi} nV_o \left| \frac{jf_n L_n Q_e + 1}{f_n^2 L_n} \right| \quad (4)$$

Therefore, the resonant capacitor voltage reaches its maximum value at the minimum switching frequency and maximum load. According to this equation, the current sensing network components can be calculated. Due to the nature of FHA, the final circuit parameters need to be verified through actual hardware test.

**Table 7-1. Calculated Current Sensing Network Components**

NAME	FUNCTION	DESIGN EQUATION
$R_s$	Transfer ac voltage across resonant capacitor into current source	$R_s = \frac{V_{Cr\_pk}(max)^2}{2P_{Rs}(max)} \quad (5)$
$C_s$	Blocking dc voltage on resonant capacitor	$C_s = \frac{10}{R_s f_{min}} \quad (6)$
$R_p$	Load resistor of the current source	$R_p = \frac{R_s}{V_{Cr\_pk}(max)} \pi \quad (7)$
$C_p$	Filter capacitor	$C_p = \frac{10}{R_p f_{min}} \quad (8)$

### 7.3.3 Gate Driver

The half-bridge resonant converter is controlled by the nearly 50% duty-cycle variable frequency square-wave voltage. This allows the half bridge to be easily driven by the gate-driver transformer. Compared with a half-bridge driver device, a gate-driver transformer provides a simple and reliable solution, which:

- Eliminates the need for gate driver power supply
- Enables simplified layout
- Prevents shoot-through due to the transformer coupling
- Requires no latch up

The UCC25600 integrates two-gate drivers with 0.4-A source and 0.8-A sink capability to directly drive the gate-driver transformer.

For the LLC resonant converter, it is critical for the gate-driver signal to be precisely symmetrical. Otherwise, the resonant tank operation will be asymmetrical. The load current distribution will be unbalanced for the output rectifiers, which in turn require the over-design of the power stages and thermal management.

In UCC25600, the gate-driver output is precisely trimmed to have less than 50-ns mismatch. Although the gate-driver signal is quite symmetrical, it is still recommended to insert the dc blocking capacitor in the gate-driver transformer primary side to prevent transformer saturation during fast transients.

### 7.3.4 Overtemperature Protection

UCC25600 continuously senses its junction temperature. When its junction temperature rises above 160°C, the device will enter overtemperature protection mode with both gate drivers actively pulled low. When junction temperature drops below 140°C, gate driver restarts with soft start.

## 7.4 Device Functional Modes

### 7.4.1 Burst-Mode Operation

During light load condition, the resonant converter tends to increase its switching frequency and maintain the output voltage regulation. However, due to ringing caused by the transformer parasitic capacitor and the rectification-diode-junction capacitors, the energy could be directly transferred to the load through these capacitors. When this power becomes more than the load requires, the output voltage become higher than the regulation level. In this case, further increasing the switching frequency will not help the situation because energy transfer to the load is not through the power stage itself.

To prevent output overvoltage during this condition, the UCC25600 includes the burst-mode operation function. When the control loop demands switching frequency higher than 350 kHz, the gate driver is disabled and the power stage stops switching. When the output voltage drops, the control loop begins to demand switching frequency less than 330 kHz, the gate driver recovers and the power stage begins to deliver power again. This allows the output voltage to be regulated.

This burst mode can be easily disabled by limiting the maximum switching frequency to less than 350 kHz. In this way, the control loop will never demand a switching frequency higher than 350 kHz and burst mode operation will not occur.

### 7.4.2 VCC

When VCC becomes above 10.5 V, the device is enabled and, after all fault conditions are cleared, the gate driver starts with soft start. When VCC drops below 9.5 V, the device enters the UVLO protection mode and both gate drivers are actively pulled low. When VCC rises above 20 V, the device enters VCC overvoltage protection mode and the device is disabled with both gate drivers actively pulled low. The VCC overvoltage protection will recover with soft start when the VCC voltage returns below 18 V.

## 8 Application and Implementation

### Note

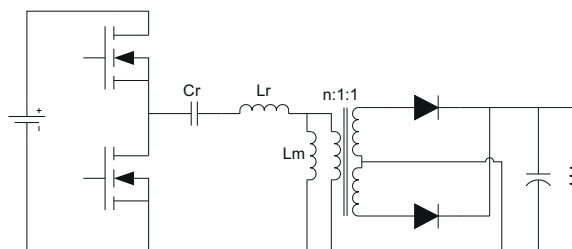
Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes, as well as validating and testing their design implementation to confirm system functionality.

### 8.1 Application Information

The UCC25600 device is a high performance, resonant-mode controller designed for DC/DC applications using resonant topologies, especially the LLC half-bridge resonant converter.

#### 8.1.1 Principal of Operation

The soft-switching capability, high efficiency, and long holdup time make the LLC resonant converter attractive for many applications, such as digital TV, ac-to-dc adapters, and computer power supplies. [Figure 8-1](#) shows the schematic of the LLC resonant converter.

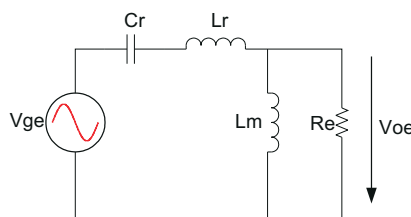


**Figure 8-1. LLC Resonant Converter**

The LLC resonant converter is based on the series resonant converter (SRC). By using the transformer magnetizing inductor, zero-voltage switching can be achieved over a wide range of input voltage and load. As a result of multiple resonances, zero-voltage switching can be maintained even when the switching frequency is higher or lower than resonant frequency. This simplifies the converter design to avoid the zero-current switching region which can lead to system damage. The converter achieves the best efficiency when operated close to its resonant frequency at a nominal input voltage. As the switching frequency is lowered, the voltage gain is significantly increased. This allows the converter to maintain regulation when the input voltage falls low. These features make the converter ideally suited to operate from the output of a high-voltage, boost PFC pre-regulator, allowing it to hold up through brief periods of ac line-voltage dropout.

Due to the nature of resonant converter, all the voltages and currents on the resonant components are approximately sinusoidal. The gain characteristic of the LLC resonant converter is analyzed based on the first harmonic approximation (FHA), which means all the voltages and currents are treated as a sinusoidal shape with the frequency the same as the switching frequency.

According to the operation principle of the converter, the LLC resonant converter can be drawn as the equivalent circuit shown in [Figure 8-2](#).



**Figure 8-2. LLC Resonant Converter Equivalent Circuit**

In this equivalent circuit, the  $V_{ge}$  and  $V_{oe}$  are the fundamental harmonics of the voltage generated by the half-bridge and the voltage on the transformer primary side, respectively. These voltages can be calculated through Fourier analysis. The load resistor  $R_e$  is the equivalent resistor of the load, and it can be calculated as:

$$R_e = \frac{8}{\pi^2} n^2 R \quad (9)$$

Based on this equivalent circuit, the converter gain at different switching frequencies can be calculated as:

$$\frac{V_o}{V_{DC}/2} = \left| \frac{\frac{j\omega L_m R_e}{j\omega L_m + R_e}}{\frac{j\omega L_m R_e}{j\omega L_m + R_e} + \frac{1}{j\omega C_r} + j\omega L_r} \right| \quad (10)$$

In this equation  $V_{DC}/2$  is the equivalent input voltage due to the half-bridge structure.

**Table 8-1. Circuit Definition Calculations**

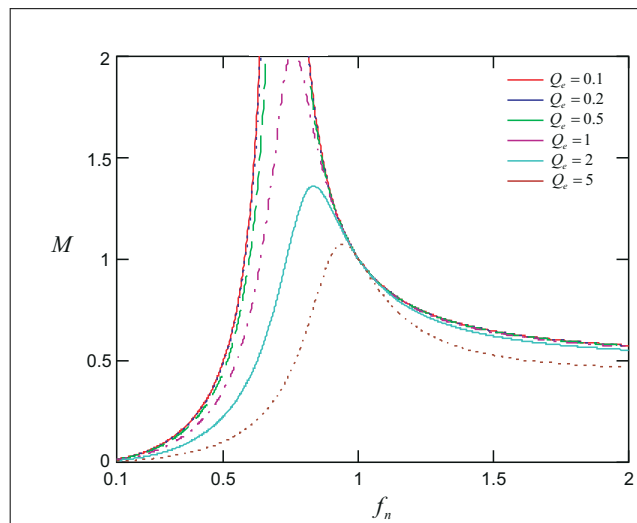
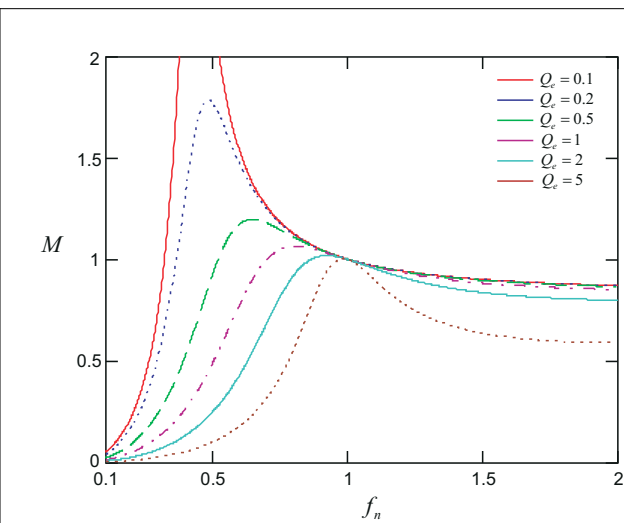
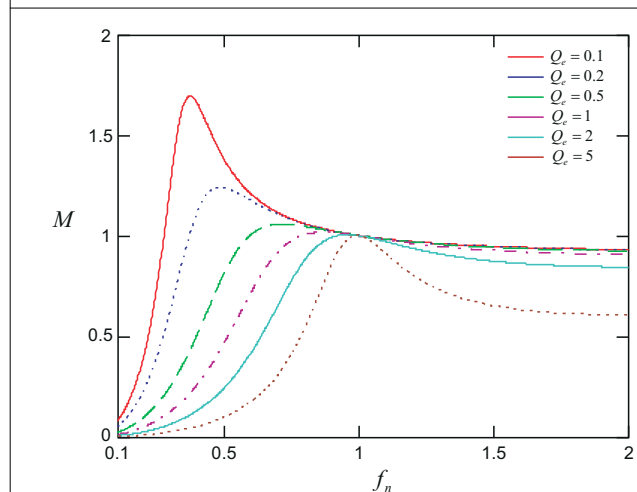
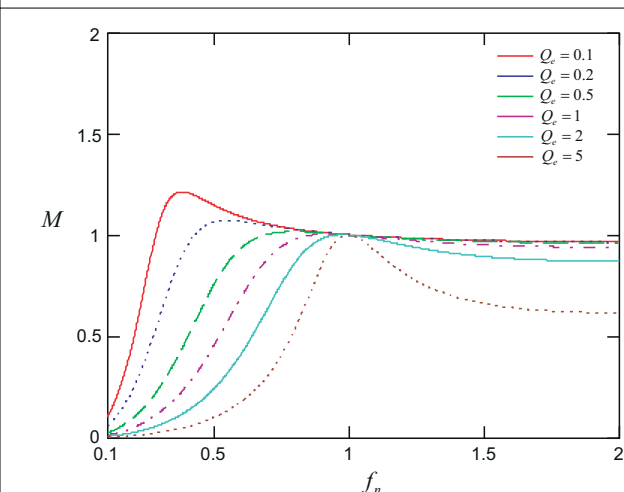
NORMALIZED GAIN	RESONANT FREQUENCY	QUALITY FACTOR	NORMALIZED FREQUENCY	INDUCTOR RATIO
$M = \frac{V_o}{V_{DC}/2} \quad (11)$	$f_0 = \frac{1}{2\pi \sqrt{L_r C_r}} \quad (12)$	$Q_e = \frac{\sqrt{L_r / C_r}}{R_e} \quad (13)$	$f_n = \frac{f}{f_0} \quad (14)$	$L_n = \frac{L_m}{L_r} \quad (15)$

Following the definitions in [Table 8-1](#), the converter gain at different switching frequencies can be written as:

$$M = \left| \frac{L_n \times f_n^2}{[(L_n + 1) \times f_n^2 - 1] + j[(f_n^2 - 1) \times f_n \times Q_e \times L_n]} \right| \quad (16)$$

Because of the FHA, this gain equation is an approximation. When the switching frequency moves away from the resonant frequency, the error becomes larger. However, this equation can be used as a design tool. The final results need to be verified by the time-based simulation or hardware test.

From Equation 16, when the switching frequency is equal to the resonant frequency,  $f_n = 1$  and converter voltage gain is equal to 1. Converter gain at different loads and inductor ratio conditions are shown in Figure 8-3 through Figure 8-6.

Figure 8-3. M vs  $f_n$ Figure 8-4. M vs  $f_n$ Figure 8-5. M vs  $f_n$ Figure 8-6. M vs  $f_n$ 

Based on its theory of operation, the LLC resonant converter is controlled through pulse frequency modulation (PFM). The output voltage is regulated by adjusting the switching frequency according to the input and output conditions. Optimal efficiency is achieved at the nominal input voltage by setting the switching frequency close to the resonant frequency. When the input voltage drops low, the switching frequency is decreased to boost the gain and maintain regulation.

The UCC25600 resonant half-bridge controller uses variable switching frequency control to adjust the resonant tank impedance and regulate output voltage. This 8-pin package device integrates the critical functions for optimizing the system performance while greatly simplifying the design and layout.



### 8.1.2 Adjustable Dead Time

Resonant half-bridge converter relies on the resonant tank current at MOSFETs turn-off to achieve soft switching and reduce switching loss. Higher turn-off current provides more energy to discharge the junction capacitor, while it generates more turn-off loss. Smaller turn-off current reduces turn-off loss, but it requires longer time to discharge MOSFETs junction capacitors and achieve soft switching. By choosing an appropriate dead time, turn-off current is minimized while still maintaining zero-voltage switching, and best system performance is realized.

In UCC25600, dead time can be adjusted through a single resistor from the DT pin to ground. With internal 2.25-V voltage reference, the current flow through the resistor sets the dead time.

$$t_d = 20ns + R_{dt} \times 24ns / k\Omega \quad (17)$$

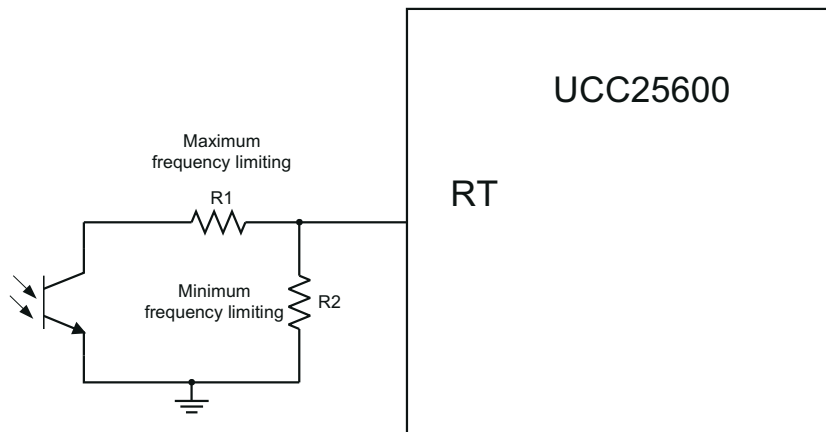
To prevent shoot through when the DT pin accidentally connects to ground, a minimum 120-ns dead time is inserted into the 2 gate driver outputs. Any dead-time setting less than 120 ns will be limited to 120 ns.

### 8.1.3 Oscillator

With variable switching frequency control, UCC25600 relies on the internal oscillator to vary the switching frequency. The oscillator is controlled by the current flowing out of the RT pin. Except during soft start, the relationship between the gate signal frequency and the current flowing out of the RT pin can be represented as:

$$f_s = \frac{1}{2} \frac{1}{\frac{6ns \times 1A}{I_{RT}} + 150ns} \approx I_{RT} \times 83Hz / \mu A \quad (18)$$

Because the switching frequency is proportional to the current, by limiting the maximum and minimum current flowing out of the RT pin, the minimum and maximum switching frequency of the converter could be easily limited. As shown in Figure 8-7, putting a resistor from the RT pin to ground limits the minimum current and putting a resistor in series with the opto-coupler limits the maximum current.



**Figure 8-7. Maximum and Minimum Frequency Setting for UCC25600**

The frequency limiting resistor can be calculated based on following equations.

$$I_{f\max} = \frac{6ns}{\frac{1}{2f_{\max}} - 150ns} \quad (19)$$

$$I_{f\min} = \frac{6ns}{\frac{1}{2f_{\min}} - 150ns} \quad (20)$$

$$I_{f\max} = 2.5V \left( \frac{1}{R_1} + \frac{1}{R_2} \right) \quad (21)$$

$$I_{f\min} = \frac{2.5V}{R_2} \quad (22)$$

## 8.2 Typical Application

This design example describes the HPA341 EVM design and outlines the design steps required to design a 300-W LLC resonant half-bridge converter, which provides a regulated output voltage nominally at 12 V at maximum 300 W of load power, with reinforced isolation of AC-DC off-line applications between the primary and the secondary, operating from a DC source of 390 V.

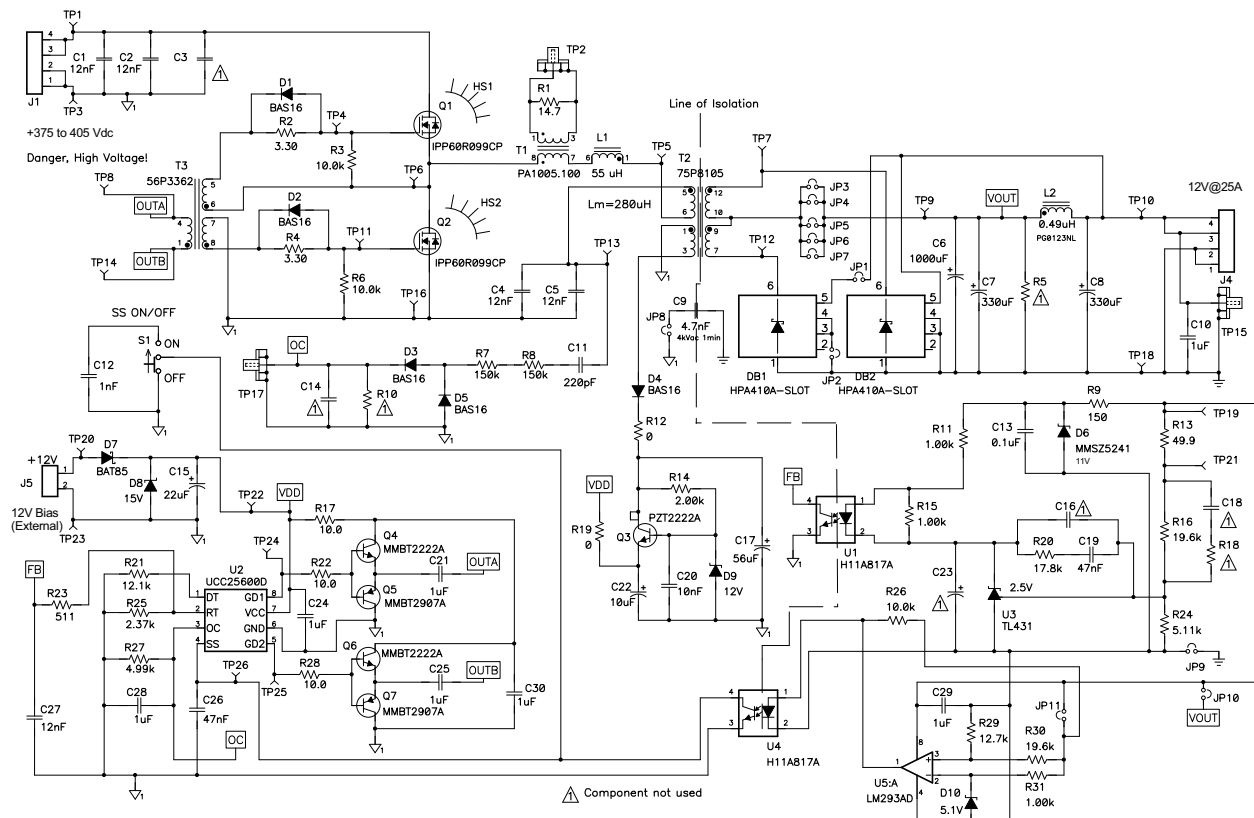


Figure 8-8. Typical Application Schematic

## 8.2.1 Design Requirements

**Table 8-2. Design Requirements**

DESIGN PARAMETER	TARGET VALUE
Output voltage	12 V
Rated output power	300 W
Input DC voltage range	375 V to 405 V
Typical efficiency at full load	91%
Switching frequency	85 kHz to 350 kHz
Resonant frequency	130 kHz

## 8.2.2 Detailed Design Procedure

1. Resonant inductor ( $L_r$ ), resonant capacitor ( $C_r$ ), and  $L_m$  of half-bridge LLC

- a. Turns ratio of Main transformer:

$$n = N_p/N_s = 16.5 \quad (23)$$

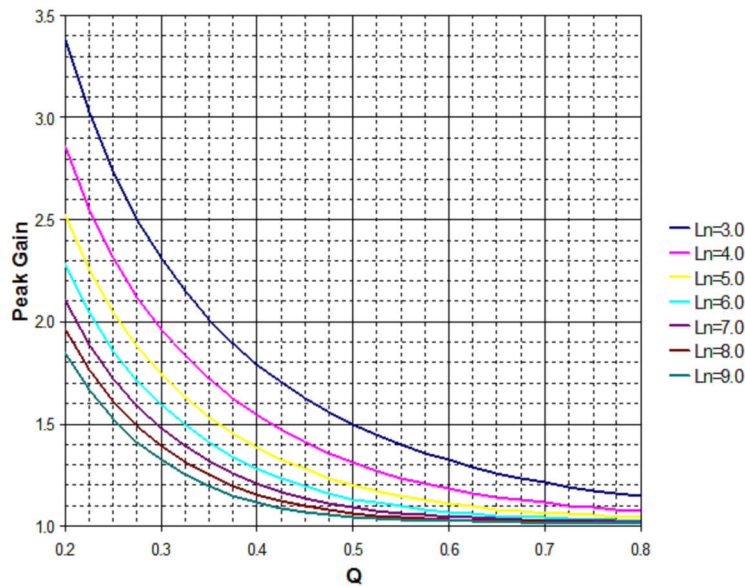
- b. Maximum resonant gain required:

$$M_{\max} = 110\% \times n \times (2 \times V_{\text{out}})/(V_{\text{in\_min}}) = 110\% \times 16.5 \times (2 \times 12 \text{ V})/375 \text{ V} = 1.17 \quad (24)$$

- c. Choose  $L_n$  and  $Q$ . The  $L_n$  range is typically selected from 3 to 9. Choose  $Q$  based on the curves below, where the peak gain must be higher than or equal to the maximum resonant gain required. Based on the below curves,  $Q$  selects 0.45.

$$L_n = L_m/L_r = 5 \quad (25)$$

$$Q = \sqrt{(L_r / C_r)} / R_{\text{eq}} = 0.45 \quad (26)$$



**Figure 8-9. Peak Gain vs Q**

- d. Calculate equivalent primary resistance:

$$R_{\text{eq}} = (8 \times n^2 \times V_{\text{out}}^2)/(\pi^2 \times P_{\text{out}}) = (8 \times 4.6^2 \times 12^2)/(\pi^2 \times 300) = 108.6\Omega \quad (27)$$

- e. Select  $C_r$ :

$$C_r = 24\text{nF} \quad (28)$$

f. Calculate  $L_r$ :

$$f_r = \frac{1}{2\pi \times \sqrt{L_r \times C_r}} \quad (29)$$

g. Combine the above two equations:

$$L_r = 55 \mu\text{H} \quad (30)$$

h. Calculate  $L_m$ :

$$L_m = L_n \times L_r = 275 \mu\text{H} \quad (31)$$

2. Calculate  $R_{dt}$ . In the UCC25600, dead time can be adjusted through a single resistor from DT pin to ground. With an internal 2.25-V voltage reference, the current flow through the resistor sets the dead time.

$$t_d = 20\text{ns} + R_{dt} \times 24\text{ns/k}\Omega \quad (32)$$

where

- $t_d = 300 \text{ ns}$
- $R_{dt} = 11.7 \text{ k}\Omega$

3. Calculate  $C_{SS}$ . Refer to [Soft Start](#) for more details.

$$t_{ss} = 25 \text{ ms} \quad (33)$$

$$t_{ss} = 2.8 \text{ V/5 } \mu\text{A} \times C_{ss} \quad (34)$$

$$C_{ss} = 44.6 \text{ nF} \quad (35)$$

4. A 47nF capacitor is selected. Calculate  $R_{T1}$  and  $R_{T2}$ . Refer to [Oscillator](#) for more details.  $R_{T1}$  and  $R_{T2}$  are used to limit maximum switching frequency and minimum switching frequency.  $R_{T1}$  and  $R_{T2}$  can be calculated based on following equations:

$$f_{\text{max}} = 6 \text{ ns}/(1/2f_{\text{max}} - 150 \text{ ns}) \quad (36)$$

$$f_{\text{min}} = 6 \text{ ns}/(1/2f_{\text{min}} - 150 \text{ ns}) \quad (37)$$

$$f_{\text{max}} = 2.5 \text{ V}/(1/R_{T1} + 1/R_{T2}) \quad (38)$$

$$f_{\text{min}} = 2.5 \text{ V}/R_{T2} \quad (39)$$

5. Combine the four equations above:

$$R_{T1} = 511\Omega \quad (40)$$

$$R_{T2} = 2.37 \text{ k}\Omega \quad (41)$$

6. Calculate  $R_s$ ,  $C_s$ ,  $R_p$ , and  $C_p$ . Refer to [Overcurrent Protection](#) for more details.

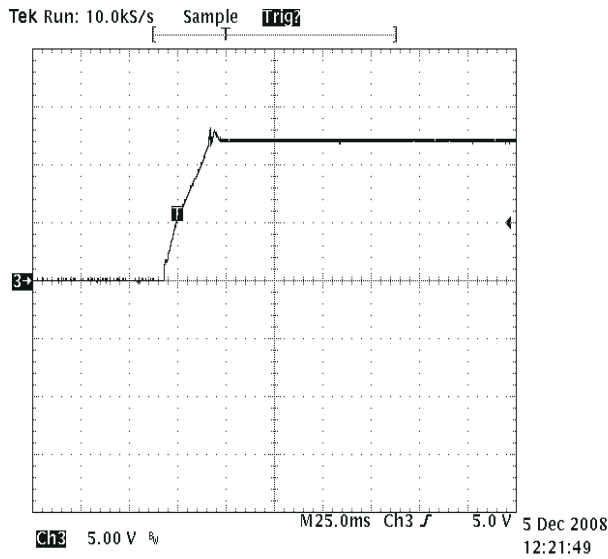
$$R_s = 300 \text{ k}\Omega \quad (42)$$

$$C_s = 22 \text{ pF} \quad (43)$$

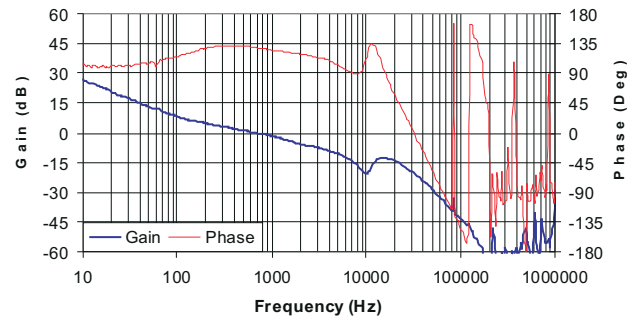
$$R_p = 4.99 \text{ k}\Omega \quad (44)$$

$$C_p = 1 \mu\text{F} \quad (45)$$

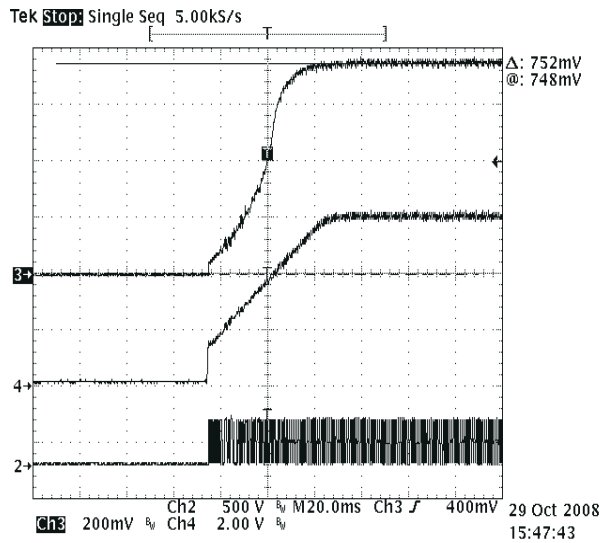
### 8.2.3 Application Curves



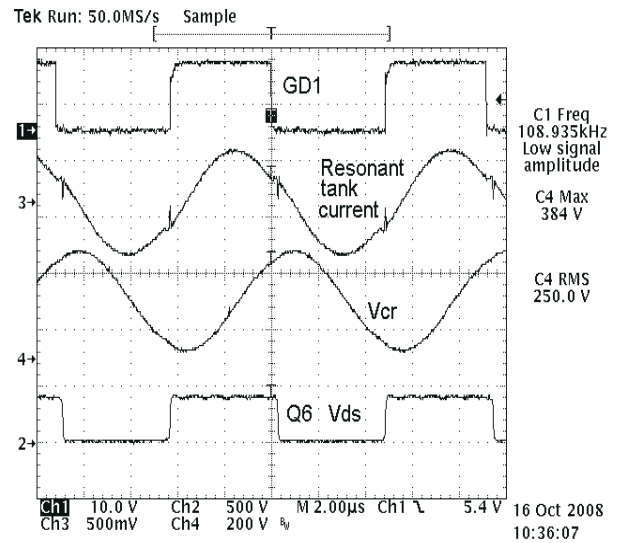
**Figure 8-10. Typical Output Voltage Turn On (TP15)**



**Figure 8-11. Full System Loop Compensation (TP19 and TP21)**



**Figure 8-12. Typical Soft-Start Waveform**



**Figure 8-13. Typical Resonant Tank Current and Resonant Capacitor Voltage**

## 9 Power Supply Recommendations

The VCC power terminal for the device requires the direct placement of low-ESR noise-decoupling capacitance from the VCC terminal to the GND terminal. Ceramic capacitors with stable dielectric characteristics over temperature are recommended, such as X7R or better. Depending on the operating temperature range of the application, X5R may be acceptable, but the drop in capacitance value at high temperature and with applied DC-bias may not be tolerable. Avoid dielectrics with poor temperature stability.

The recommended decoupling capacitor is a 1- $\mu$ F 0805-sized 50-V X7R capacitor, ideally with (but not essential) a second, smaller, parallel 100-nF 0603-sized 50-V X7R capacitor. Higher voltage-rated parts can also be used. The use of 25-V rated parts is not recommended, due to reduction in effective capacitance value with applied DC bias.

## 10 Layout

### 10.1 Layout Guidelines

A four-layer layout is recommended.

A 1- $\mu$ F ceramic decoupling capacitor is recommended, to be placed as close as possible between the VCC terminal and GND, and tracked directly to both terminals.

Place C<sub>SS</sub>, RDT, R<sub>p</sub>, C<sub>p</sub>, RT1, and RT2 as close as possible to the UCC25600.

Connect a regulated bias supply to the VCC pin.

## 10.2 Layout Example

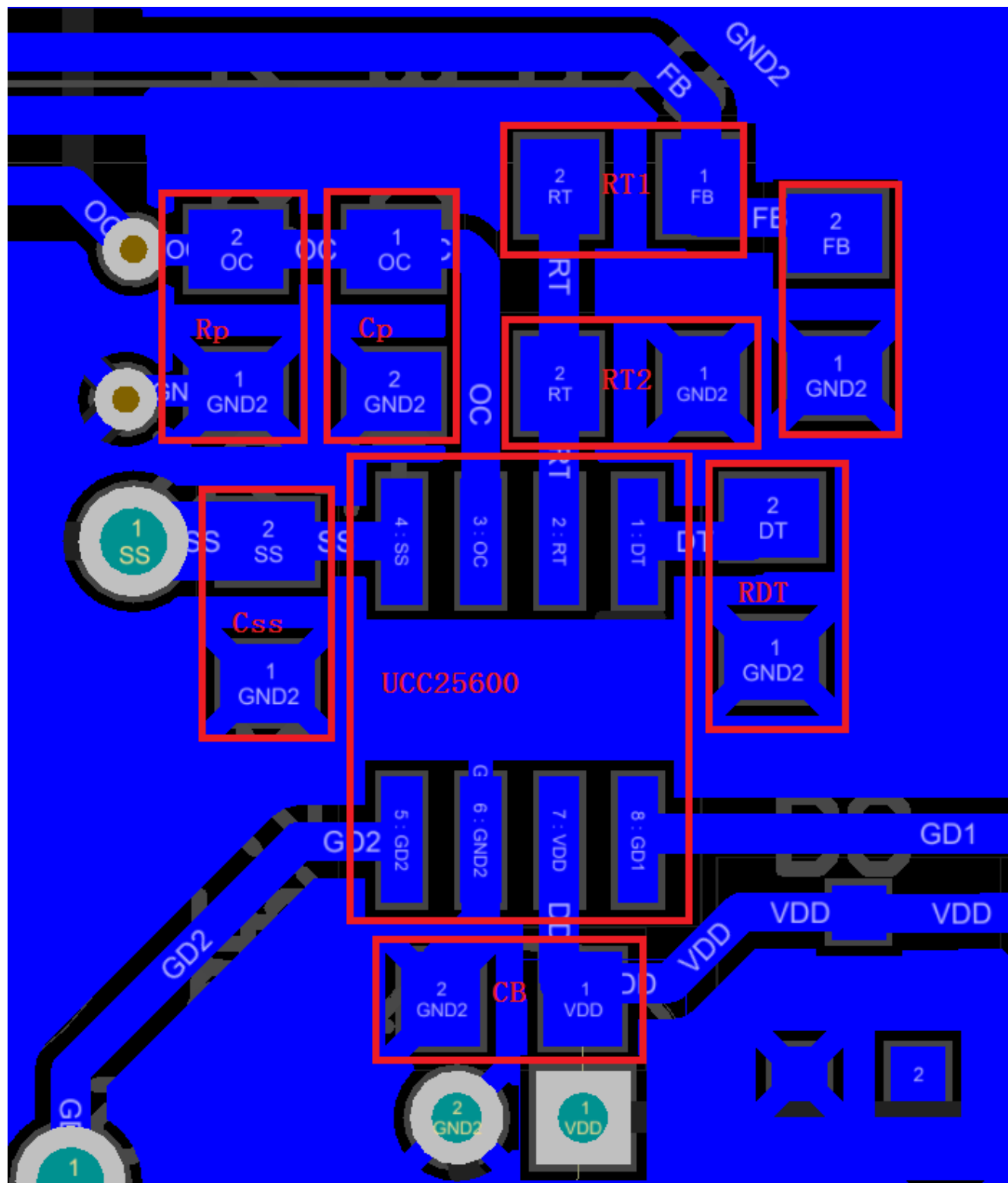


Figure 10-1. Board Layout Example

## 11 Device and Documentation Support

### 11.1 Support Resources

[TI E2E™ support forums](#) are an engineer's go-to source for fast, verified answers and design help — straight from the experts. Search existing answers or ask your own question to get the quick design help you need.

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### 11.3 Electrostatic Discharge Caution



This integrated circuit can be damaged by ESD. Texas Instruments recommends that all integrated circuits be handled with appropriate precautions. Failure to observe proper handling and installation procedures can cause damage.

ESD damage can range from subtle performance degradation to complete device failure. Precision integrated circuits may be more susceptible to damage because very small parametric changes could cause the device not to meet its published specifications.

## 12 Glossary

[TI Glossary](#) This glossary lists and explains terms, acronyms, and definitions.

## 13 Mechanical, Packaging, and Orderable Information

The following pages include mechanical, packaging, and orderable information. This information is the most current data available for the designated devices. This data is subject to change without notice and revision of this document. For browser-based versions of this data sheet, refer to the left-hand navigation.



## PACKAGING INFORMATION

Orderable part number	Status (1)	Material type (2)	Package   Pins	Package qty   Carrier	RoHS (3)	Lead finish/ Ball material (4)	MSL rating/ Peak reflow (5)	Op temp (°C)	Part marking (6)
<a href="#">UCC25600D</a>	Active	Production	SOIC (D)   8	75   TUBE	Yes	NIPDAU	Level-2-260C-1 YEAR	-40 to 125	25600
UCC25600D.A	Active	Production	SOIC (D)   8	75   TUBE	Yes	NIPDAU	Level-2-260C-1 YEAR	-40 to 125	25600
UCC25600D.B	Active	Production	SOIC (D)   8	75   TUBE	Yes	NIPDAU	Level-2-260C-1 YEAR	-40 to 125	25600
<a href="#">UCC25600DR</a>	Active	Production	SOIC (D)   8	2500   LARGE T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 125	25600
UCC25600DR.A	Active	Production	SOIC (D)   8	2500   LARGE T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 125	25600
UCC25600DR.B	Active	Production	SOIC (D)   8	2500   LARGE T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 125	25600
UCC25600DRG4	Active	Production	SOIC (D)   8	2500   LARGE T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 125	25600

(1) **Status:** For more details on status, see our [product life cycle](#).

(2) **Material type:** When designated, preproduction parts are prototypes/experimental devices, and are not yet approved or released for full production. Testing and final process, including without limitation quality assurance, reliability performance testing, and/or process qualification, may not yet be complete, and this item is subject to further changes or possible discontinuation. If available for ordering, purchases will be subject to an additional waiver at checkout, and are intended for early internal evaluation purposes only. These items are sold without warranties of any kind.

(3) **RoHS values:** Yes, No, RoHS Exempt. See the [TI RoHS Statement](#) for additional information and value definition.

(4) **Lead finish/Ball material:** Parts may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

(5) **MSL rating/Peak reflow:** The moisture sensitivity level ratings and peak solder (reflow) temperatures. In the event that a part has multiple moisture sensitivity ratings, only the lowest level per JEDEC standards is shown. Refer to the shipping label for the actual reflow temperature that will be used to mount the part to the printed circuit board.

(6) **Part marking:** There may be an additional marking, which relates to the logo, the lot trace code information, or the environmental category of the part.

Multiple part markings will be inside parentheses. Only one part marking contained in parentheses and separated by a "~" will appear on a part. If a line is indented then it is a continuation of the previous line and the two combined represent the entire part marking for that device.

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## TAPE AND REEL INFORMATION



\*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
UCC25600DR	SOIC	D	8	2500	330.0	12.4	6.4	5.2	2.1	8.0	12.0	Q1

## TAPE AND REEL BOX DIMENSIONS



\*All dimensions are nominal

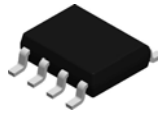
Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
UCC25600DR	SOIC	D	8	2500	353.0	353.0	32.0

## TUBE

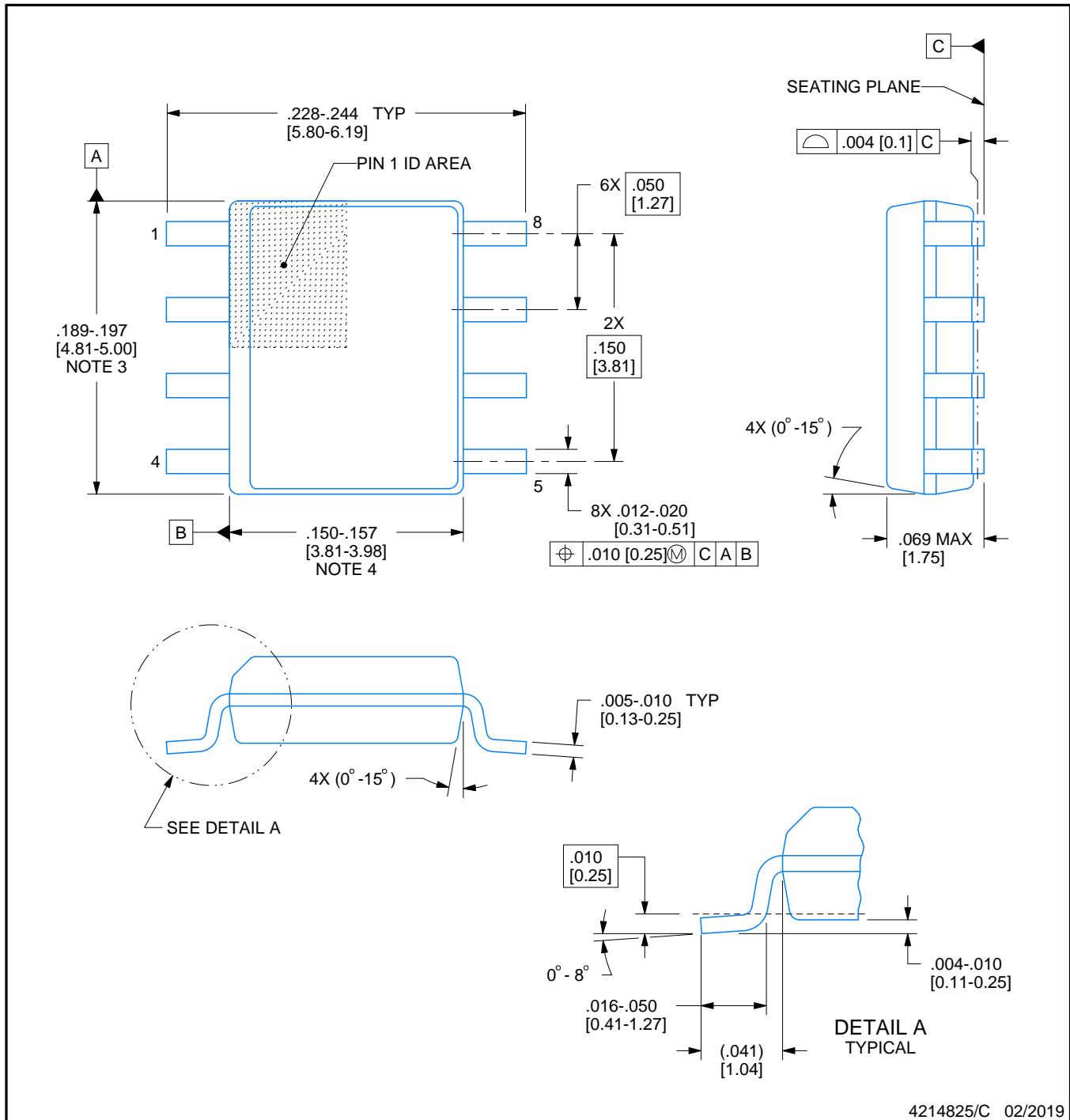


\*All dimensions are nominal

Device	Package Name	Package Type	Pins	SPQ	L (mm)	W (mm)	T (μm)	B (mm)
UCC25600D	D	SOIC	8	75	506.6	8	3940	4.32
UCC25600D.A	D	SOIC	8	75	506.6	8	3940	4.32
UCC25600D.B	D	SOIC	8	75	506.6	8	3940	4.32

**D0008A****PACKAGE OUTLINE****SOIC - 1.75 mm max height**

SMALL OUTLINE INTEGRATED CIRCUIT



4214825/C 02/2019

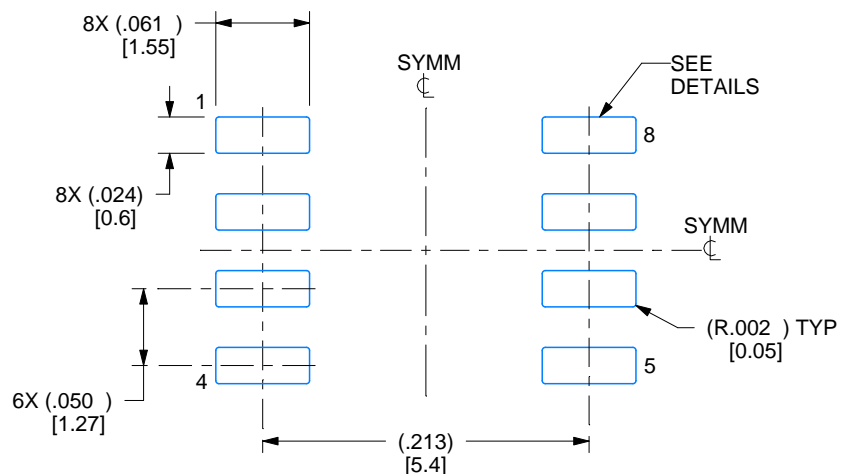
**NOTES:**

- Linear dimensions are in inches [millimeters]. Dimensions in parenthesis are for reference only. Controlling dimensions are in inches. Dimensioning and tolerancing per ASME Y14.5M.
- This drawing is subject to change without notice.
- This dimension does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed .006 [0.15] per side.
- This dimension does not include interlead flash.
- Reference JEDEC registration MS-012, variation AA.

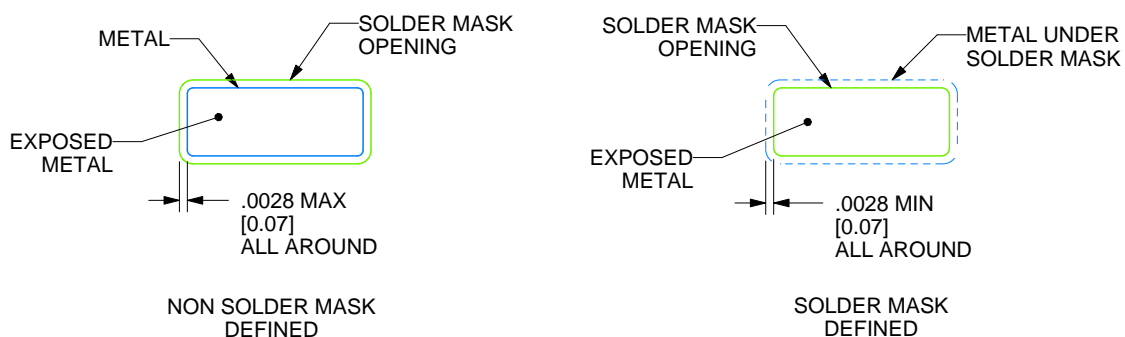
**D0008A**

## SOIC - 1.75 mm max height

## SMALL OUTLINE INTEGRATED CIRCUIT



LAND PATTERN EXAMPLE  
EXPOSED METAL SHOWN  
SCALE:8X



## SOLDER MASK DETAILS

4214825/C 02/2019

NOTES: (continued)

6. Publication IPC-7351 may have alternate designs.

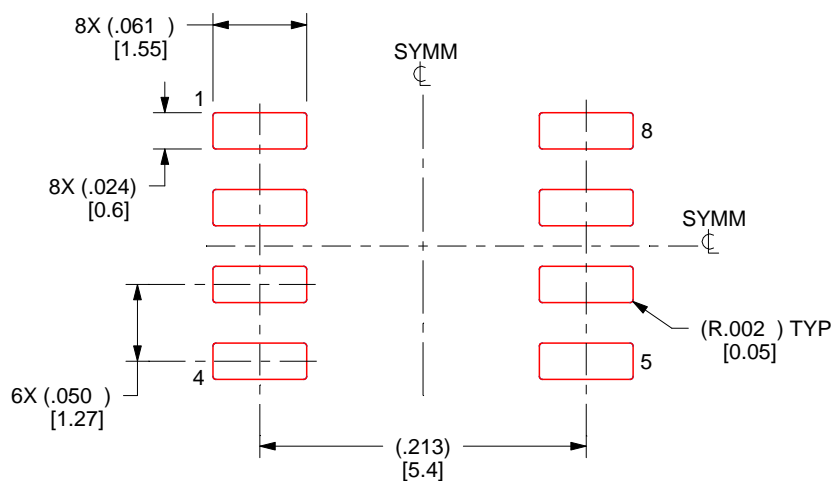
7. Solder mask tolerances between and around signal pads can vary based on board fabrication site.

## EXAMPLE STENCIL DESIGN

D0008A

SOIC - 1.75 mm max height

SMALL OUTLINE INTEGRATED CIRCUIT



SOLDER PASTE EXAMPLE  
BASED ON .005 INCH [0.125 MM] THICK STENCIL  
SCALE:8X

4214825/C 02/2019

NOTES: (continued)

8. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.
9. Board assembly site may have different recommendations for stencil design.



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