

TPS75003 構成可能なマルチレールPMIC

1 特長

- 2つの効率95%の3A降圧コンバータと1つの300mA LDO
- Xilinxにより、Spartan™-3、Spartan-3E、Spartan-3L FPGAの給電用にテスト済みで推奨
- すべてのチャンネルの出力電圧は可変（降圧で1.2V～6.5V、LDOで1.0V～6.5V）
- 入力電圧範囲: 2.2V～6.5V
- 各電源に独立のソフトスタート
- 各電源に独立のイネーブルによる柔軟なシーケンシング
- LDOは2.2μFのセラミック出力コンデンサで安定
- 小さく薄型の4.5mm×3.5mm×0.9mmのVQFNパッケージ

2 アプリケーション

- FPGA、DSP、ASICの電源
- セットトップ・ボックス
- DSLモデム
- プラズマ・テレビのディスプレイ・パネル

3 概要

TPS75003はFPGA、DSP、その他のマルチ電源アプリケーション向けの包括的な電源管理ソリューションです。このデバイスは、Xilinx Spartan-3、Spartan-3E、Spartan-3Lのスタートアップ・プロファイル要件について、単調増加の電圧ランプや電圧レールの最小立ち上がり時間も含めてすべてテスト済みで、満たしています。各出力に独立のイネーブルが存在するため、シーケンシングが可能で、スタートアップ時の電源の要求を最小化できます。各電源のソフトスタート機能により、スタートアップ時の突入電流が制限されます。2つの内蔵降圧コントローラにより、コアとI/Oなど、小電流と大電流の両方の電源について効率的でコスト効果の優れた電圧変換が可能です。内蔵の300mA LDOにより、Xilinx Spartan-3 FPGAのV_{CCAUX}などの補助レールを供給できます。3つの出力電圧はすべて外部で構成可能なため、最大の柔軟性が得られます。

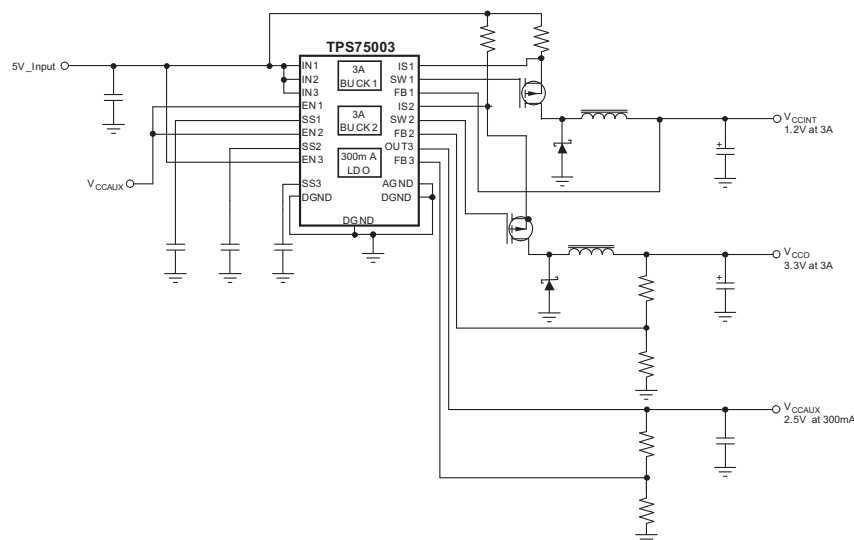
TPS75003は-40°C～+85°Cで完全に動作が規定されており、VQFNパッケージで供給されるため、ソリューション全体が非常に小型になり、高い電力放散能力が得られます。

製品情報⁽¹⁾

型番	パッケージ	本体サイズ(公称)
TPS75003	VQFN (20)	4.50mm×3.50mm

(1) 利用可能なすべてのパッケージについては、このデータシートの末尾にある注文情報を参照してください。

代表的なアプリケーションの回路図



目次

1	特長	1	8	Application and Implementation	15
2	アプリケーション	1	8.1	Application Information	15
3	概要	1	8.2	Typical Application	16
4	改訂履歴	2	9	Power Supply Recommendations	22
5	Pin Configuration and Functions	3	10	Layout	23
6	Specifications	4	10.1	Layout Guidelines	23
6.1	Absolute Maximum Ratings	4	10.2	Layout Example	24
6.2	ESD Ratings	4	11	デバイスおよびドキュメントのサポート	25
6.3	Recommended Operating Conditions	4	11.1	デバイス・サポート	25
6.4	Thermal Information	5	11.2	ドキュメントのサポート	25
6.5	Electrical Characteristics	5	11.3	ドキュメントの更新通知を受け取る方法	25
6.6	Typical Characteristics	6	11.4	コミュニティ・リソース	25
7	Detailed Description	10	11.5	商標	25
7.1	Overview	10	11.6	静電気放電に関する注意事項	25
7.2	Functional Block Diagram	11	11.7	Glossary	25
7.3	Feature Description	11	12	メカニカル、パッケージ、および注文情報	26

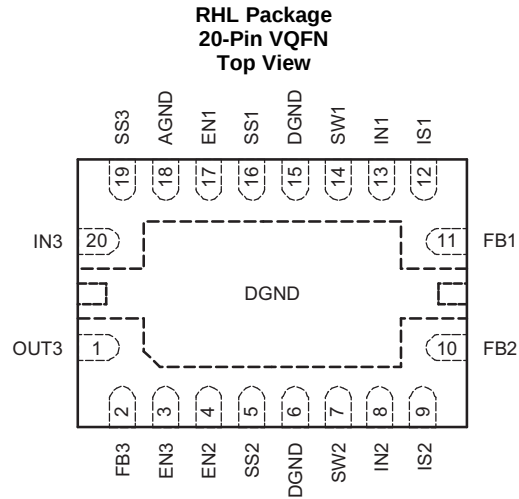
4 改訂履歴

資料番号末尾の英字は改訂を表しています。その改訂履歴は英語版に準じています。

Revision I (August 2010) から Revision J に変更	Page
• 最新のTIデータシートのフォーマットに合わせてフォーマットを更新、データシートのタイトルを 変更	1
• Moved the ESD rating parameters for HBM and CDM from the <i>Absolute Maximum Ratings</i> table to the <i>ESD Ratings</i> table	4
• Added the <i>Recommended Operating Conditions</i> table, <i>Overview</i> section, <i>Feature Description</i> section, <i>Design Requirements</i> section, <i>Power Supply Recommendations</i> section, and <i>Device and Documentation Support</i> section	4
• Updated the symbols for the thermal resistance parameters in the <i>Thermal Information</i> table	5

Revision H (August 2008) から Revision I に変更	Page
• Replaced the <i>Dissipation Ratings</i> table with the <i>Thermal Information</i> table	5

5 Pin Configuration and Functions



Pin Functions

PIN		TYPE	DESCRIPTION
NAME	NO.		
AGND	18	GND	Ground connection for LDO.
DGND	6, 15, PAD	GND	Ground connection for BUCK1 and BUCK2 converters. Pins 6 and 15 should be connected to the back side exposed pad by a short metal trace as shown in the PCB Layout Considerations section of this data sheet.
EN1	17	I	Driving the enable pin (ENx) high turns on BUCK1 regulator. Driving this pin low puts it into shutdown mode, reducing operating current. The enable pin does not trigger on fast negative going transients.
EN2	4	I	Same as EN1 but for BUCK2 controller.
EN3	3	I	Same as EN1 but for LDO.
FB1	11	I (Analog)	Feedback pin. Used to set the output voltage of BUCK1 regulator.
FB2	10	I (Analog)	Same as FB1 but for BUCK2 controller.
FB3	2	I (Analog)	Same as FB1 but for LDO.
IN1	13	I (Analog)	Input supply to BUCK1.
IN2	8	I (Analog)	Input supply to BUCK2.
IN3	20	I (Power)	Input supply to LDO.
IS1	12	I (Analog)	Current sense input for BUCK1 regulator. The voltage difference between this pin and IN1 is compared to an internal reference to set current limit. For a robust output start-up ramp, careful layout and bypassing are required. See the Application Information section for details.
IS2	9	I (Analog)	Same as IS1 but compared to IN2 and used for BUCK2 controller.
OUT3	1	O (Power)	Regulated LDO output. A small ceramic capacitor ($\geq 2.2\mu\text{F}$) is needed from this pin to ground to ensure stability.
SS1	16	I (Analog)	Connecting a capacitor between this pin and ground increases start-up time of the BUCK1 regulator by slowing the ramp-up of current limit. This high-impedance pin is noise-sensitive; careful layout is important. See the Typical Characteristics , Application Information , and PCB Layout Considerations sections for details.
SS2	5	I (Analog)	Same as SS1 but for BUCK2 regulator.
SS3	19	I (Analog)	Connecting a capacitor from this pin to ground slows the start-up time of the LDO reference, thereby slowing output voltage ramp-up. See the Application Information section for details.
SW1	14	O (Analog)	Gate drive pin for external BUCK1 P-channel MOSFET.
SW2	7	O (Analog)	Same as SW1 but for BUCK2 controller.

6 Specifications

6.1 Absolute Maximum Ratings

Over operating free-air temperature range (unless otherwise noted)⁽¹⁾

		MIN	MAX	UNIT
V _{INX}	IN1, IN2, IN3 voltage	−0.3	7	V
V _{ENX}	EN1, EN2, EN3 voltage	−0.3	V _{INX} + 0.3	V
V _{SWX}	SW1, SW2, SW3 voltage	−0.3	V _{INX} + 0.3	V
V _{ISX}	IS1, IS2, IS3 voltage	−0.3	V _{INX} + 0.3	V
V _{OUT3}	OUT3 voltage	−0.3	7	V
V _{SSX}	SS1, SS2, SS3 voltage	−0.3	V _{INX} + 0.3	V
V _{FBX}	FB1, FB2, FB3 voltage	−0.3	3.3	V
I _{OUT3}	Peak LDO output current	Internally limited		
	Continuous total power dissipation	See Thermal Information Table		
T _J	Junction temperature	−55	150	°C
T _{stg}	Storage temperature	−65	150	°C

- (1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only, which do not imply functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Conditions*. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.

6.2 ESD Ratings

		VALUE	UNIT
V _(ESD)	Electrostatic discharge	Human-body model (HBM), per ANSI/ESDA/JEDEC JS-001 ⁽¹⁾	1000
		Charged-device model (CDM), per JEDEC specification JESD22-C101 ⁽²⁾	500

- (1) JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process.
 (2) JEDEC document JEP157 states that 250-V CDM allows safe manufacturing with a standard ESD control process.

6.3 Recommended Operating Conditions

over operating free-air temperature range (unless otherwise noted)

		MIN	NOM	MAX	UNIT
V _{IN1}	Input voltage at IN1 pin	2.2		6.5	V
V _{OUT1}	Output voltage of BUCK1	1.2		V _{IN1}	V
I _{OUT1}	Maximum output current of BUCK1			3	A
V _{IN2}	Input voltage at IN2 pin	2.2		6.5	V
V _{OUT2}	Output voltage of BUCK1	1.2		V _{IN2}	V
I _{OUT2}	Maximum output current of BUCK2			3	A
V _{IN3}	Input voltage at IN3 pin	2.2		6.5	V
V _{OUT3}	Output voltage of LDO	1		V _{IN3} − V _{DO}	V
I _{OUT3}	Maximum output current of LDO			300	mA

6.4 Thermal Information

THERMAL METRIC ⁽¹⁾		TPS75003	UNIT
		RHL (VQFN)	
		20 PINS	
R _{θJA}	Junction-to-ambient thermal resistance	42.6	°C/W
R _{θJC(top)}	Junction-to-case (top) thermal resistance	51.8	°C/W
R _{θJB}	Junction-to-board thermal resistance	39.5	°C/W
ψ _{JT}	Junction-to-top characterization parameter	0.6	°C/W
ψ _{JB}	Junction-to-board characterization parameter	14.2	°C/W
R _{θJC(bot)}	Junction-to-case (bottom) thermal resistance	2.8	°C/W

(1) For more information about traditional and new thermal metrics, see the [Semiconductor and IC Package Thermal Metrics application report](#).

6.5 Electrical Characteristics

V_{EN1} = V_{IN1}, V_{EN2} = V_{IN2}, V_{EN3} = V_{IN3}, V_{IN1} = V_{IN2} = 2.2V, V_{IN3} = 3.0V, V_{OUT3} = 2.5V, C_{OUT1} = C_{OUT2} = 47μF, C_{OUT3} = 2.2μF, T_A = –40°C to +85°C, unless otherwise noted. Typical values are at T_A = +25°C.

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
Supply and Logic						
V _{INX}	Input Voltage Range (IN1, IN2, IN3) ⁽¹⁾		2.2		6.5	V
I _Q	Quiescent Current, I _Q = I _{DGND} + I _{AGND}	I _{OUT1} = I _{OUT2} = 0mA, I _{OUT3} = 1mA		75	150	μA
I _{SHDN}	Shutdown Supply Current	V _{EN1} = V _{EN2} = V _{EN3} = 0V		0.05	3	μA
V _{IH1, 2}	Enable High, enabled (EN1, EN2)		1.4		V _{INX}	V
V _{IH3}	Enable High, enabled (EN3)		1.14		V _{IN3}	V
V _{ILX}	Enable Low, shutdown (EN1, EN2, EN3)		0		0.3	V
I _{ENX}	Enable pin current (EN1, EN2, EN3)			0.01	0.5	μA
Buck Controllers 1 and 2						
V _{OUT1,2}	Adjustable Output Voltage Range ⁽²⁾		V _{FBX}		V _{INX}	V
V _{FB1,2}	Feedback Voltage (FB1, FB2)		1.220			V
	Feedback Voltage Accuracy ⁽¹⁾ (FB1, FB2)		−2%		2%	
I _{FB1,2}	Current into FB1, FB2 pins		0.01		0.5	μA
V _{IS1,2}	Reference Voltage for Current Sense		80	100	120	mV
I _{IS1,2}	Current into IS1, IS2 Pins		0.01		0.5	μA
ΔV _{OUT} %/ΔV _{IN}	Line Regulation ⁽¹⁾	Measured with the circuit in Figure 18, V _{OUT} + 0.5V ≤ V _{IN} ≤ 6.5V	0.1			%/V
ΔV _{OUT} %/ΔI _{OUT} _T	Load Regulation	Measured with the circuit in Figure 18, 30mA ≤ I _{OUT} ≤ 2A	0.6			%/A
η _{1,2}	Efficiency ⁽³⁾	Measured with the circuit in Figure 18, I _{OUT} = 1A	94%			
t _{STR1,2}	Startup Time ⁽³⁾	Measured with the circuit in Figure 18, R _L = 6Ω, C _{OUT} = 100μF, C _{SS} = 2.2nF	5			ms

(1) To be in regulation, minimum V_{IN1} (or V_{IN2}) must be greater than V_{OUT1,NOM} (or V_{OUT2,NOM}) by an amount determined by external components. Minimum V_{IN3} = V_{OUT3} + V_{DO} or 2.2V, whichever is greater.

(2) Maximum V_{OUT} depends on external components and will be less than V_{IN}.

(3) Depends on external components.

Electrical Characteristics (continued)

$V_{EN1} = V_{IN1}$, $V_{EN2} = V_{IN2}$, $V_{EN3} = V_{IN3}$, $V_{IN1} = V_{IN2} = 2.2V$, $V_{IN3} = 3.0V$, $V_{OUT3} = 2.5V$, $C_{OUT1} = C_{OUT2} = 47\mu F$, $C_{OUT3} = 2.2\mu F$, $T_A = -40^\circ C$ to $+85^\circ C$, unless otherwise noted. Typical values are at $T_A = +25^\circ C$.

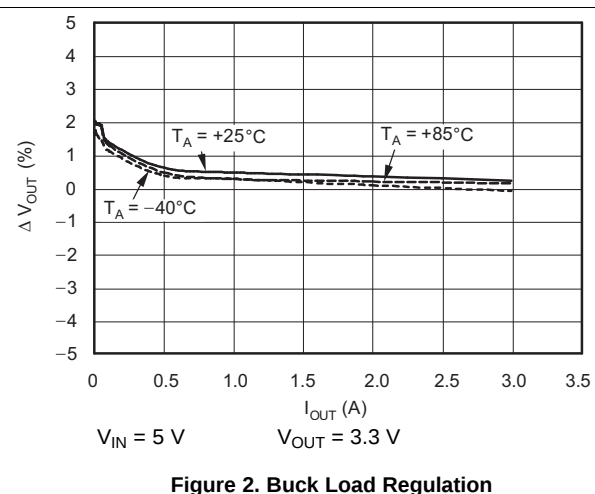
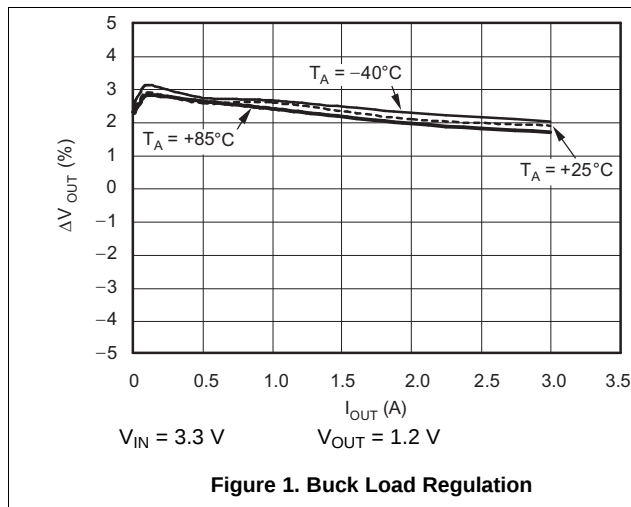
PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
R _{DS,ON1,2}	Gate Driver P-Channel and N-Channel MOSFET On-Resistance	V _{IN1,2} > 2.5V	4			Ω
		V _{IN1,2} = 2.2V	6			
I _{SW1,2}	Gate Driver P-Channel and N-Channel MOSFET Drive Current		100			mA
t _{ON}	Minimum On Time		1.36	1.55	1.84	μs
t _{OFF}	Minimum Off Time		0.44	0.65	0.86	μs
LDO						
V _{OUT3}	Output Voltage Range		1	6.5 – V _{DO}		V
V _{FB3}	Feedback Pin Voltage		0.507			V
	Feedback Pin Voltage Accuracy ⁽¹⁾	2.95V ≤ V _{IN3} ≤ 6.5V 1mA ≤ I _{OUT3} ≤ 300mA	–4%		4%	
ΔV _{OUT%} /ΔV _{IN}	Line Regulation ⁽¹⁾	V _{OUT3} + 0.5V ≤ V _{IN3} ≤ 6.5V	0.075			%/V
ΔV _{OUT%} /ΔI _{OUT}	Load Regulation	10mA ≤ I _{OUT3} ≤ 300mA	0.01			%/mA
V _{DO}	Dropout Voltage (V _{IN} = V _{OUT(NOM)} – 0.1) ⁽⁴⁾	I _{OUT3} = 300mA	250		350	mV
I _{CL3}	Current Limit	V _{OUT} = 0.9 × V _{OUT(NOM)}	375	600	1000	mA
I _{FB3}	Current into FB3 pin		0.03		0.1	μA
V _n	Output Noise	BW = 100Hz – 100kHz, I _{OUT3} = 300mA	400			μV _{RMS}
t _{SD}	Thermal Shutdown Temperature for LDO	Shutdown, Temp Increasing	175			°C
		Reset, Temp Decreasing	160			
UVLO	Under-Voltage Lockout Threshold	V _{IN} Rising	1.80			V
	Under-Voltage Lockout Hysteresis	V _{IN} Falling	100			mV

(4) V_{DO} does not apply when $V_{OUT} + V_{DO} < 2.2V$.

6.6 Typical Characteristics

Measured using circuit in [Figure 18](#).

6.6.1 Buck Converter



Buck Converter (continued)

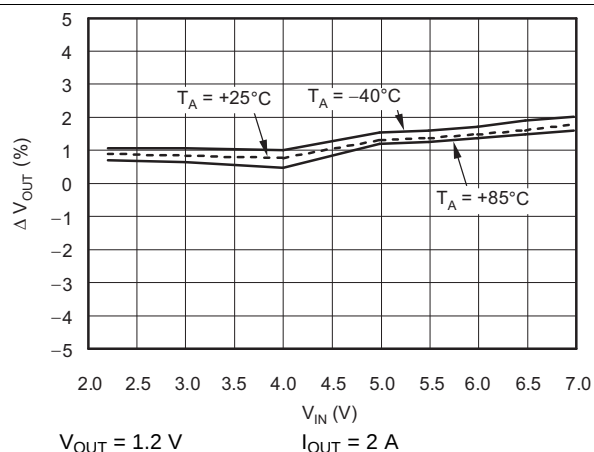


Figure 3. Buck Line Regulation

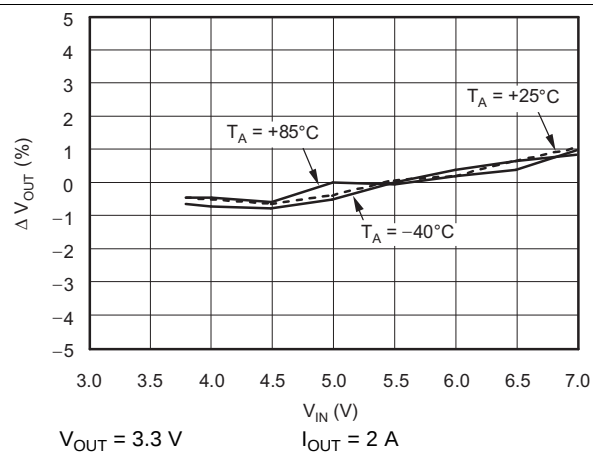


Figure 4. Buck Line Regulation

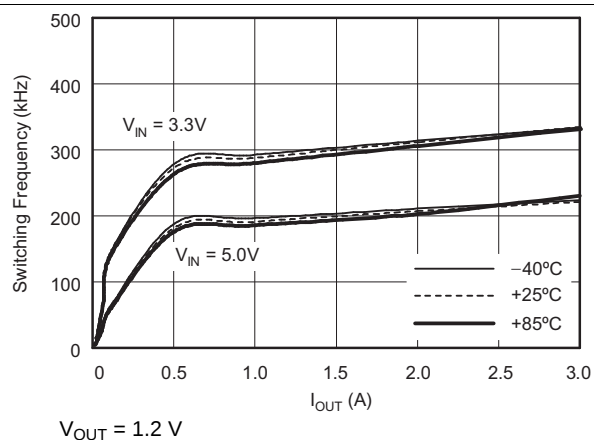


Figure 5. Buck Switching Frequency vs I_{OUT} , T_A

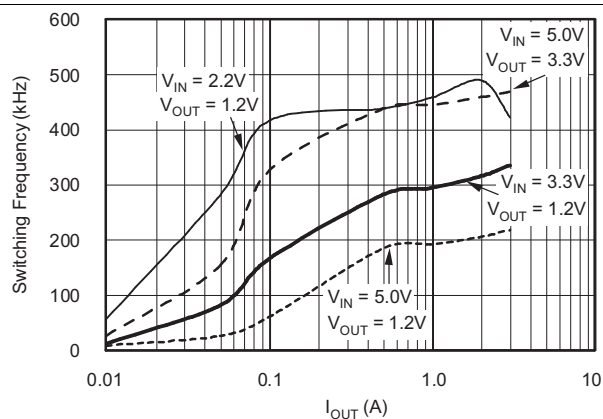


Figure 6. Buck Switching Frequency vs I_{OUT}

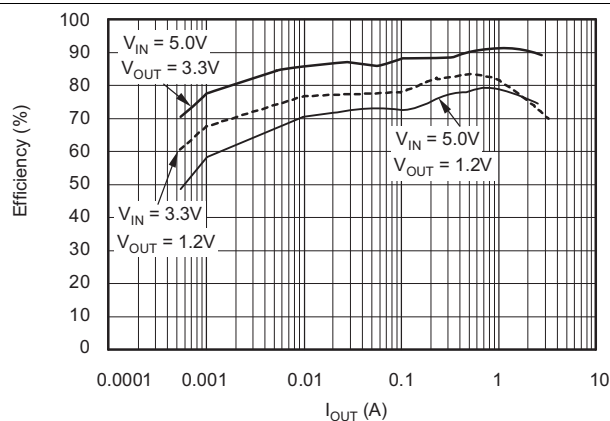


Figure 7. Efficiency vs I_{OUT}

6.6.2 LDO Converter

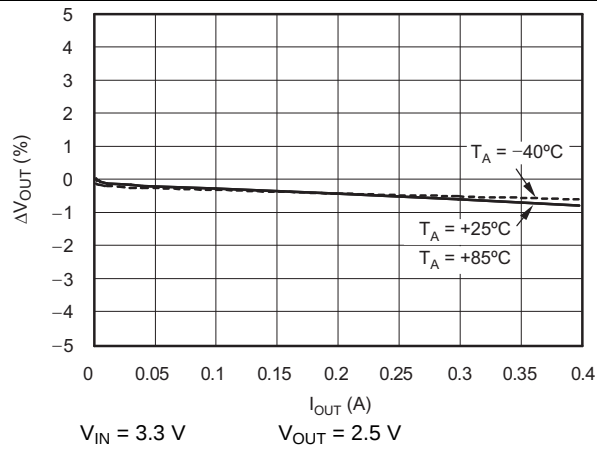


Figure 8. LDO Load Regulation

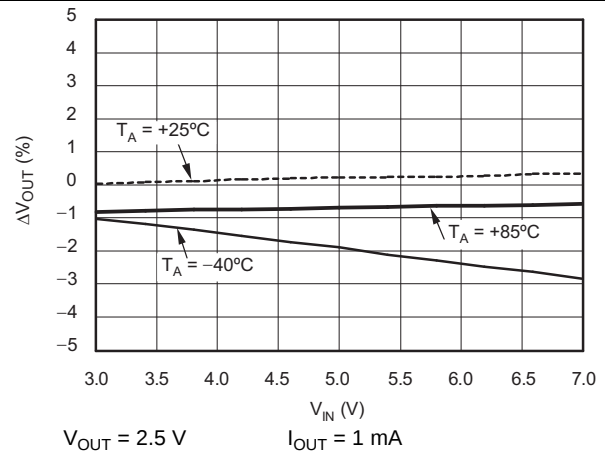


Figure 9. LDO Line Regulation

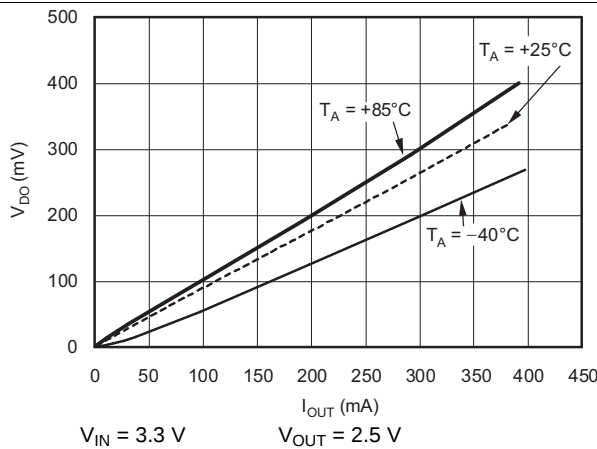


Figure 10. LDO Dropout vs I_{OUT}

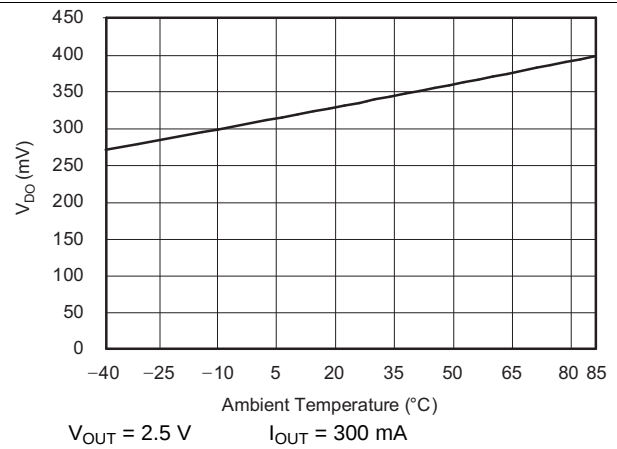


Figure 11. LDO Dropout vs T_A

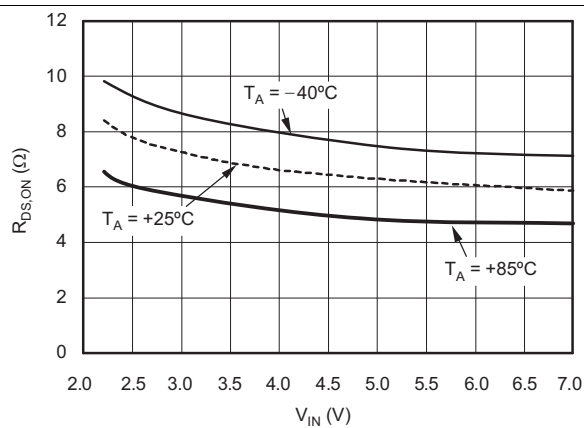


Figure 12. $R_{DS,ON}$ PMOS vs V_{IN}

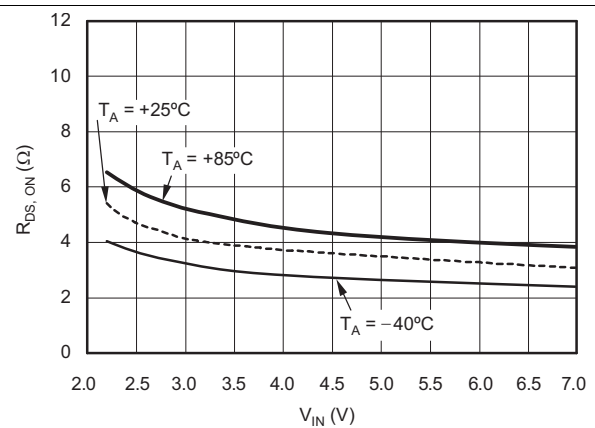


Figure 13. $R_{DS,ON}$ NMOS vs V_{IN}

LDO Converter (continued)

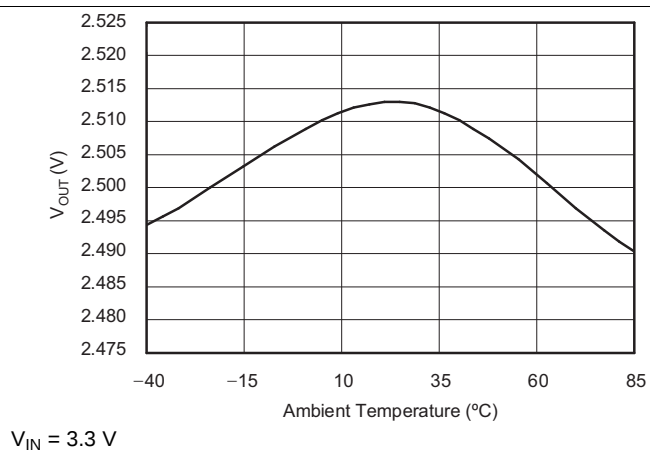


Figure 14. LDO V_{OUT} vs T_A

7 Detailed Description

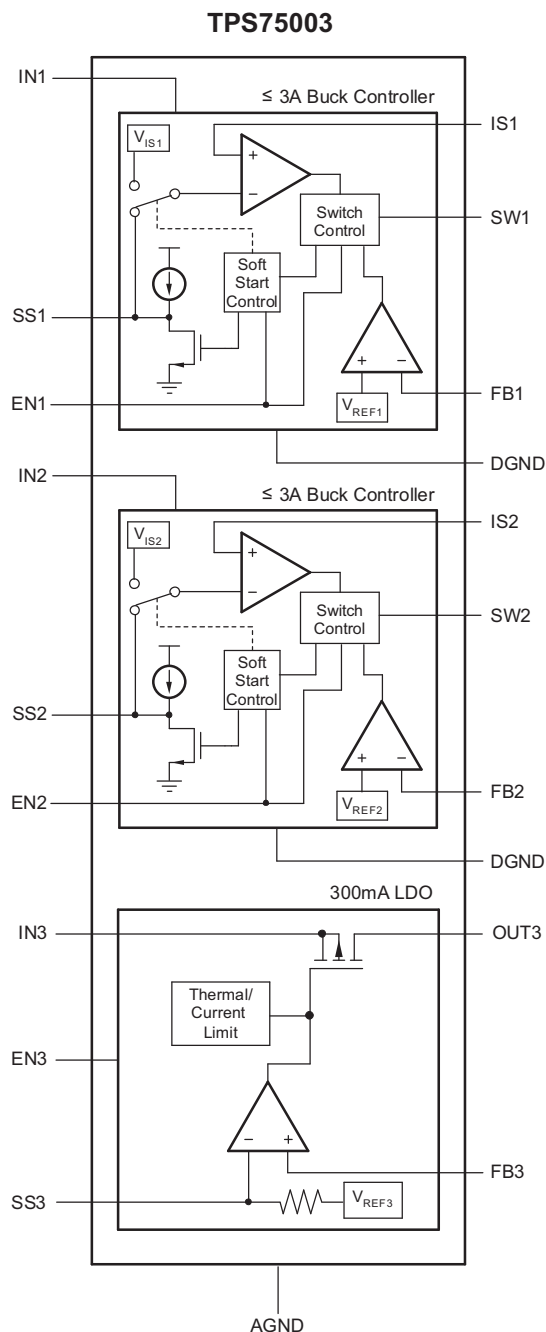
7.1 Overview

The TPS75003 device is a power management IC (PMIC) with two buck controllers and one integrated LDO regulator. The three voltage regulators have independent enable pins for flexible power sequence timing, and all of the output voltages are set by external feedback resistor dividers. The independent power regulators can be wired in parallel, in series, or connected to separate input voltages as needed to meet the requirements of the application.

The two buck controllers are identical and operate over a input voltage range of 2.2 V to 6.5 V to supply a load with an externally configurable output voltage with up to 3-A of current. The buck controllers drive the gate of a single PMOS FET in an asynchronous buck regulator architecture. The use of a PMOS FET lets the buck regulator operate with 100% duty cycle when the input voltage is approximately equal to or less than the desired output voltage. The buck controllers have an externally configurable current sense feature to limit the output current and protect the PMOS FET. The buck controllers have an externally configurable soft-start feature that ramps the voltage and meet the timing requirements of the load.

The LDO regulator integrates the FET and operates over the same input voltage range of 2.2 V to 6.5 V to supply a load with an externally configurable output voltage with up to 300-mA of current. The LDO regulator includes integrated current limiting and thermal protection features. The LDO regulator also has an externally configurable soft-start feature to ramp the voltage to meet desired timing requirements.

7.2 Functional Block Diagram



7.3 Feature Description

7.3.1 Operation (Buck Controllers)

Channels 1 and 2 have two identical non-synchronous buck controllers that use minimum on-time and minimum off-time hysteretic control (see Figure 18. For clarity, BUCK1 is used throughout the discussion of device operation. When V_{OUT1} is less than its target, an external PMOS (Q1) is turned on for at least the minimum on-time, increasing current through the inductor (L1) until V_{OUT1} reaches its target value or the current limit (set by R1) is reached. When either of these conditions is met, the PMOS is switched off for at least the minimum off-time of the device. After the minimum off-time has passed, the output voltage is monitored and the switch is turned on again when necessary.

Feature Description (continued)

When output current is low, the buck controllers operate in discontinuous mode. In this mode, each switching cycle begins at zero inductor current, rises to a maximum value, then falls back to zero current. When current reaches zero on the falling edge, ringing occurs at the resonant frequency of the inductor and stray switch node capacitance. This operation is normal; it does not affect circuit performance, and can be minimized if desired by using an RC snubber, a resistor in series with the gate of the PMOS, or both as shown in [Figure 15](#).

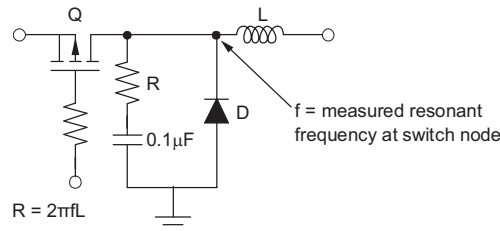


Figure 15. RC Snubber and Series Gate Resistor Used to Minimize Ringing

At higher output currents, the TPS75003 device operates in continuous mode. In continuous mode, there is no ringing at the switch node and V_{OUT} is equal to V_{IN} times the duty cycle of the switching waveform.

When V_{IN} approaches or falls to less than V_{OUT} , the buck controllers operate in 100% duty cycle mode, fully turning on the external PMOS to let regulation occur at a lower dropout than would otherwise be possible.

7.3.2 Enable (Buck Controllers)

The enable pins (EN1 and EN2) for the buck controllers are active high. When the enable pin is driven low and input voltage is present at IN1 or IN2, an on-chip FET is turned on to discharge the soft-start pin SS1 or SS2, respectively. If the soft-start feature is being used, enable should be driven high at least 10 μs after V_{IN} is applied to make sure that this discharge cycle occurs.

7.3.3 UVLO (Buck Controllers)

The device has an undervoltage lockout circuit to prevent the turnon of the external PMOS (Q1 or Q2) until a reliable operating voltage is reached on the appropriate regulator (IN1 or IN2). This prevents the buck controllers from misoperation at low input voltages.

7.3.4 Current Limit (Buck Controllers)

An external resistor (R1 or R2) is used to set the current limit for the external PMOS transistor (Q1 or Q2). These resistors are connected between IN1 and IS1 (or IN2 and IS2) to provide a reference voltage across these pins that is proportional to the current flowing through the PMOS transistor. This reference voltage is compared to an internal reference to determine if an overcurrent condition exists. When current limit is exceeded, the external PMOS is turned off for the minimum off-time. Current limit detection is disabled for 10ns any time the PMOS is turned on to avoid triggering on switching noise. In 100% duty cycle mode, current limit is always enabled. Current limit is calculated using the V_{IS1} or V_{IS2} specification in the [Electrical Characteristics](#) section as shown in [Equation 1](#).

$$I_{LIMIT} = \frac{V_{IS1,2}}{R_{1,2}} \quad (1)$$

The current limit resistor must be appropriately rated for the dissipated power determined by its RMS current calculated by [Equation 2](#).

$$I_{RMS} \approx I_{OUT} \sqrt{D} = I_{OUT} \sqrt{\frac{V_{OUT}}{V_{IN}}}$$

$$P_{DISS} = (I_{RMS})^2 \times R \quad (2)$$

Feature Description (continued)

For low-cost applications the $I_{S1,2}$ pin can be connected to the drain of the PMOS, using $R_{DS,ON}$ instead of R1 or R2 to set current limit. Variations in the PMOS $R_{DS,ON}$ must be considered to make sure that current limit will protect external components such as the inductor, the diode, and the switch itself from damage as a result of overcurrent.

7.3.5 Short-Circuit Protection (Buck Controllers)

In an overload condition, the current rating of the external components (PMOS, diode, and inductor) can be exceeded. To help guard against this, the TPS75003 device increases its minimum off-time when the voltage at the feedback pin is less than the reference voltage. When the output is shorted (V_{FB} is zero), the minimum off-time is increased to approximately 4 μ s. The increase in off-time is proportional to the difference between the voltage at the feedback pin and the internal reference.

7.3.6 Soft-Start (Buck Controllers)

The buck controllers each have independent soft-start capability to limit inrush during start-up and to meet timing requirements of the Xilinx Spartan-3 FPGA. Limiting inrush current by using soft-start, or by staggering the turnon of power rails, also guards against voltage drops at the input source due to its output impedance. Refer to the soft-start circuitry shown in Figure 16 and the soft-start timing diagram shown in Figure 17. The BUCK1 controller is discussed in this section; it is identical to BUCK2. Note that pins SS1 and SS2 are very high-impedance and cannot be probed using a typical oscilloscope setup. When input voltage is applied at IN1 and EN1 is driven low, any charge on the SS pin is discharged by an on-chip pulldown transistor. When EN1 is driven high, an on-chip current source starts charging the external soft-start capacitor C_{SS1} . The voltage on the capacitor is compared to the voltage across the current sense resistor R1 to determine if an overcurrent condition exists. If the voltage drop across the sense resistor becomes greater than the reference voltage, then the external PMOS is shut off for the minimum off-time. This implementation provides a cycle-by-cycle current limit and lets the user configure the soft-start time over a wide range for most applications. For detailed information on selecting C_{SS1} and C_{SS2} , see the [Soft-Start Capacitor Selection \(Buck Controllers\)](#) section.

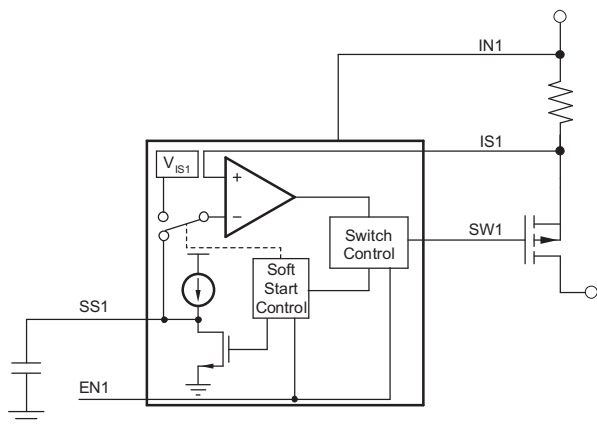


Figure 16. Soft-Start Circuitry

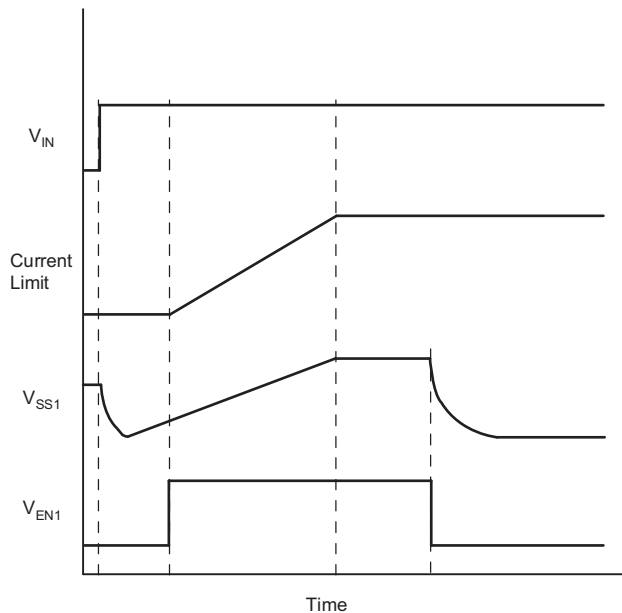


Figure 17. Soft-Start Timing Diagram

7.3.7 LDO Operation

The TPS75003 LDO regulator uses a PMOS pass transistor and is offered in an adjustable version to easily configure any output voltage. When used to power $V_{CC,AUX}$ the LDO regulator output voltage is set to 2.5V; the LDO regulator can optionally be set to other output voltages to power other circuitry. The LDO regulator has integrated soft-start, independent enable, and short-circuit and thermal protection. The LDO regulator can be used to power $V_{CC,AUX}$ on the Xilinx Spartan-3 FPGA when 3.3V JTAG signals are used as described in the [Using 3.3-V Signals for Spartan-3 Configuration and JTAG Ports application note](#).

7.3.8 Internal Current Limit (LDO)

The internal current limit of the LDO regulator helps protect the regulator during fault conditions. When an overcurrent condition is detected, the output voltage is decreased until the current falls to a level that will not damage the device. For good device reliability, the LDO regulator should not operate at the current limit.

7.3.9 Enable Pin (LDO)

The active high enable pin (EN3) can be used to put the device into shutdown mode. If shutdown and soft-start capability are not required, EN3 can be tied to IN3.

7.3.10 Dropout Voltage (LDO)

The LDO regulator uses a PMOS transistor to achieve low dropout. When $(V_{IN} - V_{OUT})$ is less than the dropout voltage (V_{DO}), the pass transistor is in its linear region of operation, and the input-output resistance is the $R_{DS,ON}$ of the pass transistor. In this region, the LDO regulator is said to be out of regulation; ripple rejection, line regulation, and load regulation degrade as $(V_{IN} - V_{OUT})$ decreases to much lower than 0.5V.

7.3.11 Transient Response (LDO)

The LDO regulator does not have an on-chip pulldown circuit for output is overvoltage conditions. This feature lets the device be used in applications that connect higher voltage sources such as an alternate power supply to the output. This design also results in an output overshoot of several percent if the load current quickly drops to zero. The amplitude of overshoot can be reduced by increasing C_{OUT} ; the duration of overshoot can be decreased by adding a load resistor.

7.3.12 Thermal Protection (LDO)

Thermal protection disables the output when the junction temperature, T_J , reaches unsafe levels. When the junction temperature cools, the output is enabled again. The thermal protection circuit may cycle on and off depending on the power dissipation, thermal resistance, and ambient temperature. This cycling limits the dissipation of the regulator, protecting it from damage. For good long term reliability, the device should not be continuously operated at or near thermal shutdown.

7.3.13 Power Dissipation (LDO)

The TPS75003 device is available in a QFN-style package with an exposed lead frame on the package underside. The exposed lead frame is the primary path for removing heat and should be soldered to a PC board that is configured to remove the amount of power dissipated by the LDO regulator, as calculated by [Equation 3](#).

$$P_D = (V_{IN3} - V_{OUT3}) \times I_{OUT3} \quad (3)$$

Power dissipation can be minimized by using the lowest possible input voltage necessary to ensure the required output voltage. The two buck converters do not contribute a significant amount of dissipated power. Using heavier copper will increase the overall effectiveness of removing heat from the device. The addition of plated through-holes to heat-dissipating layers will also improve the heatsink effectiveness.

8 Application and Implementation

NOTE

Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes. Customers should validate and test their design implementation to confirm system functionality.

8.1 Application Information

The TPS75003 is an integrated power management IC designed specifically to power DSPs and FPGAs such as the Xilinx Spartan-3, Spartan-3E and Spartan-3L. Two non-synchronous buck controllers can be configured to supply up to 3A for both CORE and I/O rails. A low dropout linear regulator powers auxiliary rails up to 300mA. All channels have independent enable and soft-start, allowing control of inrush current and output voltage ramp time as required by the application.

Table 1 through Table 4 show component values that have been tested for use with up to 3A load currents. Inductors in Table 1 are tested up to the respective saturation currents. Other similar external components can be substituted as desired; however, in all cases the circuits that are used should be tested for compliance to application requirements.

Table 1. Inductors Tested with the TPS75003

PART NUMBER	MANUFACTURER	INDUCTANCE	DC RESISTANCE	SATURATION CURRENT
SLF7032T-100M1R4	TDK	10 μ H $\pm$ 20%	53m Ω $\pm$ 20%	1.4A
SLF6025-150MR88	TDK	15 μ H $\pm$ 20%	85m Ω $\pm$ 20%	0.88A
CDRH6D28-5R0	Sumida	5 μ H	23m Ω	2.4A
CDRH6D38-5R0	Sumida	5 μ H	18m Ω	2.9A
CDRH103R-100	Sumida	10 μ H	45m Ω	2.4A
CDRH4D28-100	Sumida	10 μ H	96m Ω	1.0A
CDRH8D43-150	Sumida	15 μ H	42m Ω	2.9A
CDRH5D18-6R2	Sumida	6.2 μ H	71m Ω	1.4A
DO3316P-472	Coilcraft	4.7 μ H	18m Ω	5.4A
MSS7341-153	Coilcraft	15 μ H	55m Ω	1.6A
MSS7341-223	Coilcraft	22 μ H	82m Ω	1.26A
744052006	Würth	6.2 μ H	80m Ω	1.45A
74451115	Würth	15 μ H	90m Ω	0.8A

Table 2. PMOS Transistors Tested with the TPS75003

PART NUMBER	MANUFACTURER	R _{DS,ON} (TYP)	V _{DS}	I _D	PACKAGE
SI5457DC-T1-GE3	Vishay	0.056 Ω at VGS = -2.5V	-20V	-6A at +25°C	1206-8
SI2301BDS-T1-E3	Vishay	0.15 Ω at VGS = -2.5V	-20V	-2.0A at +25°C	SOT-23
SI2323DS-T1-E3	Vishay	0.052 Ω at VGS = -2.5V	-20V	-4.1A at +25°C	SOT-23
FDG328P	Fairchild	0.12 Ω at VGS = -2.5V	-20V	-1.5A	SC70-6

Table 3. Diodes Tested with the TPS75003

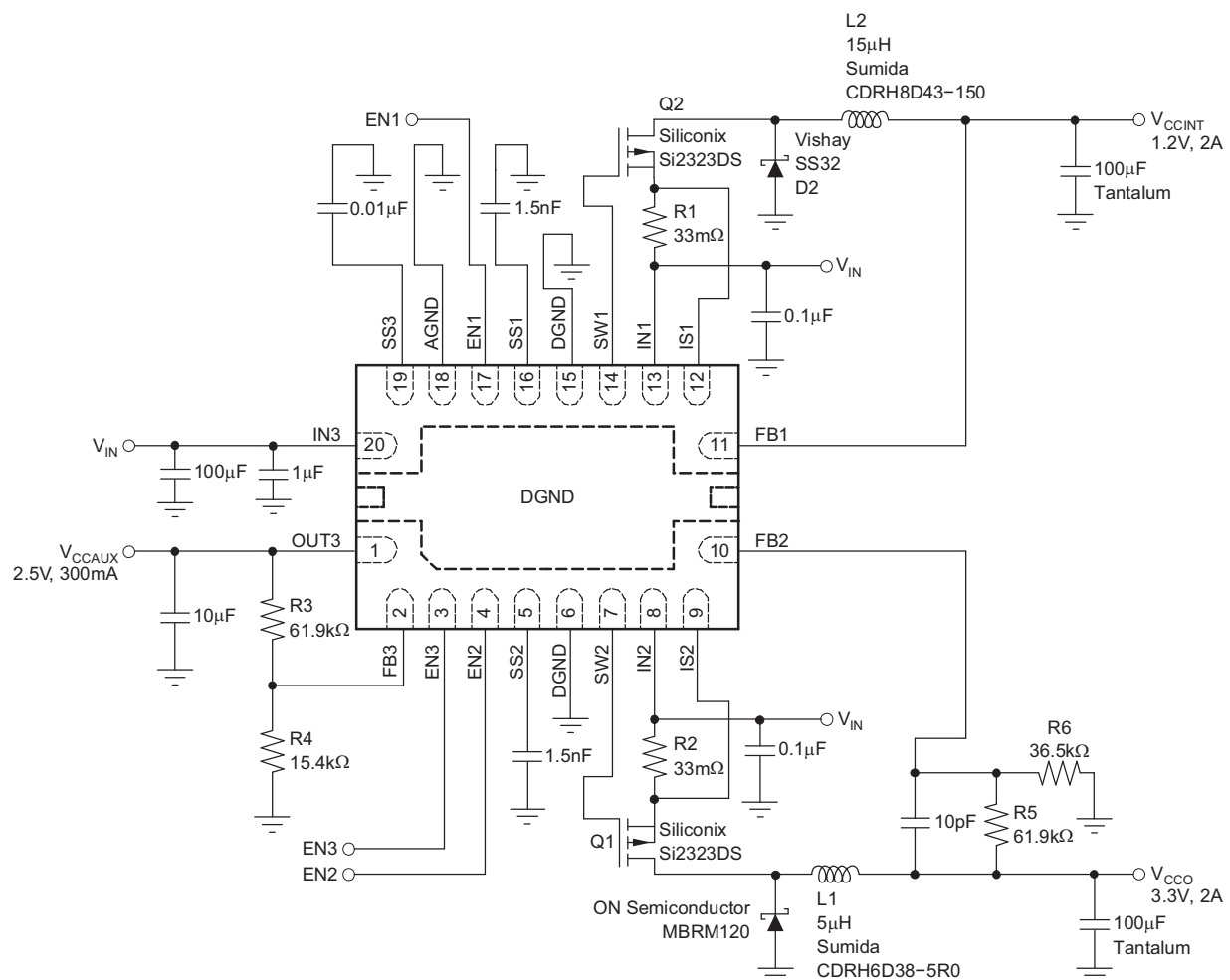
PART NUMBER	MANUFACTURER	V _R	I _F	PACKAGE
FSV240AF	ON Semiconductor / Fairchild	40V	2.0A	DO-214-2
FSV340FP	ON Semiconductor / Fairchild	40V	3.0A	SOD-123-2
SS32	ON Semiconductor / Fairchild	20V	3.0A	DO-214AB
ZHCS2000TA	Zetex	40V	2.0A	SOT-23-6
B320AE-13	Diodes Inc.	20V	3.0A	SMA

Table 4. Capacitors Tested with the TPS75003

PART NUMBER	MANUFACTURER	CAPACITANCE	ESR	VOLTAGE RATING
10TPB47M (PosCap)	Panasonic	47 μ F	0.07 Ω	10V
T491D476M010AT	Kemet	47 μ F	0.8 Ω	10V
T495D476K016ATE180	Kemet	47 μ F	0.18 Ω	16V
TR3C476K016C0300	Vishay	47 μ F	0.3 Ω	16V
T495D107M006ATE050	Kemet	100 μ F	0.05 Ω	6.3V
TPSC107M006R0075	AVX	100 μ F	0.075 Ω	6.3V
6TPE100MPB (PosCap)	Panasonic	100 μ F	0.025 Ω	6.3V
TR3C107K6R3C0125	Vishay	100 μ F	0.25 Ω	6.3V

8.2 Typical Application

Figure 18 shows a typical application circuit for powering the Xilinx Spartan-3 FPGA.


Figure 18. Typical Application Circuit for Powering the Xilinx Spartan-3 FPGA

Typical Application (continued)

8.2.1 Design Requirements

Table 5 lists the design requirements that are met by the application shown in Figure 18

Table 5. Design Parameters for Xilinx Spartan-3 FPGA Design

PARAMETER	DESCRIPTION	VALUE	UNIT
V _{IN}	Input power supply to all regulators: BUCK1 (IN1), BUCK2 (IN2), and LDO (IN3)	3.3 to 6.5	V
V _{OUT1}	Output of BUCK1 regulator V _{CCINT} , core rail power for the FPGA	1.2	V
I _{OUT1}	Load current of FPGA for V _{CCINT} rail	2	A
V _{OUT2}	Output of BUCK2 regulator V _{CCO} , I/O rail power for the FPGA	3.3	V
I _{OUT2}	Load current of FPGA for V _{CCO} rail	2	A
V _{OUT3}	Output of LDO regulator V _{CCAUX} , auxiliary rail power for the FPGA	2.5	V
I _{OUT3}	Load current of FPGA for V _{CCAUX} rail	300	mA

8.2.2 Detailed Design Procedure

8.2.2.1 Input Capacitor C_{IN1}, C_{IN2} Selection (Buck Controllers)

It is good analog design practice to place input capacitors near the inputs of the device in order to ensure a low impedance input supply. 10μF to 22μF of capacitance for each buck converter is adequate for most applications, and should be placed within 100mils (0.01in, or 2.54mm) of the IN1 and IN2 pins to minimize the effects of pulsed current switching noise on the soft-start circuitry during the first ~1V of output voltage ramp. Low ESR capacitors also help to minimize noise on the supply line. The minimum value of capacitance can be estimated using Equation 4:

$$C_{IN, MIN} + \frac{(1/2)L \times (\Delta I_L)^2}{V_{(RIPPLE)} \times V_{IN}} \approx \frac{(1/2)L \times (0.3 \times I_{OUT})^2}{V_{(RIPPLE)} \times V_{IN}} \quad (4)$$

Note that the capacitors must be able to handle the RMS current in continuous conduction mode, which can be calculated using Equation 5:

$$I_{C,IN(RMS)} \approx I_{OUT} \sqrt{\left(\frac{V_{OUT}}{V_{IN,MIN}} \right)} \quad (5)$$

8.2.2.2 Inductor Value Selection (Buck Controllers)

The inductor is chosen based on inductance value and maximum current rating. Larger inductors reduce current ripple (and therefore, output voltage ripple) but are physically larger and more expensive. Inductors with lower DC resistance typically improve efficiency, but also have higher cost and larger physical size. The buck converters work well with inductor values between 4.7μH and 47μH in most applications. When selecting an inductor, the current rating should exceed the current limit set by R_{IS} or R_{DS,ON} (see the [Current Limit \(Buck Controllers\)](#) section). To determine the minimum inductor size, first determine if the device will operate in minimum on-time or minimum off-time mode. The device will operate in minimum on-time mode if Equation 6 is satisfied:

$$V_{IN} - V_{OUT} - I_{OUT} \times R_{DS,ON} - R_L \times I_{OUT} \geq \frac{t_{OFF,MIN} \times (V_{OUT} + V_{SCHOTTKY} + R_L \times I_{OUT})}{t_{ON,MIN}}$$

where

- R_L = the inductor DC resistance

Minimum inductor size needed when operating in minimum on-time mode is given by Equation 7:

$$L_{\text{MIN}} = \frac{(V_{\text{IN}} - V_{\text{OUT}} - I_{\text{OUT}} \times R_{\text{DS,ON}} - R_{\text{L}} \times I_{\text{OUT}}) \times t_{\text{ON,MIN}}}{\Delta I_{\text{L}}} \quad (7)$$

Minimum inductor size needed when operating in minimum off-time mode is given by [Equation 8](#):

$$L_{\text{MIN}} = \frac{(V_{\text{OUT}} + V_{\text{SCHOTTKY}} + R_{\text{L}} \times I_{\text{OUT}}) \times t_{\text{OFF,MIN}}}{\Delta I_{\text{L}}}$$

where

- $\Delta I_{\text{L}} = (20\% - 30\%) \times I_{\text{OUT-MAX}}$ (8)

8.2.2.3 External PMOS Transistor Selection (Buck Controllers)

The external PMOS transistor is selected based on threshold voltage (V_{T}), on-resistance ($R_{\text{DS,ON}}$), gate capacitance (C_{G}) and voltage rating. The PMOS V_{T} magnitude must be much lower than the lowest voltage at IN1 or IN2 that will be used. A V_{T} magnitude that is 0.5V less than the lowest input voltage is normally sufficient. The PMOS gate will see voltages from 0V to the maximum input voltage, so gate-to-source breakdown should be a few volts higher than the maximum input supply. The drain-to-source of the device will also see this full voltage swing, and should therefore be a few volts higher than the maximum input supply. The RMS current in the PMOS can be estimated by using [Equation 9](#):

$$I_{\text{PMOS(RMS)}} \approx I_{\text{OUT}} \sqrt{D} = I_{\text{OUT}} \sqrt{\frac{V_{\text{OUT}}}{V_{\text{IN}}}} \quad (9)$$

The power dissipated in the PMOS is comprised of both conduction and switching losses. Switching losses are typically insignificant. The conduction losses are a function of the RMS current and the $R_{\text{DS,ON}}$ of the PMOS, and are calculated by [Equation 10](#):

$$P_{(\text{cond})} = (I_{\text{OUT}} \sqrt{D})^2 \times R_{\text{DS,ON}} \times (1 + \text{TC} \times [T_{\text{J}} - 25^{\circ}\text{C}]) \approx (I_{\text{OUT}} \sqrt{D}) \times R_{\text{DS,ON}} \quad (10)$$

8.2.2.4 Diode Selection (Buck Controllers)

The diode is off when the PMOS is on, and on when the PMOS is off. Since it will be turned on and off at a relatively high frequency, a Schottky diode is recommended for good performance. The peak current rating of the diode should exceed the peak current limit set by the sense resistor $R_{\text{IS1,2}}$. A diode with low reverse leakage current and low forward voltage at operating current will optimize efficiency. [Equation 11](#) calculates the estimated average power dissipation:

$$I_{(\text{diode})(\text{RMS})} \approx I_{\text{OUT}} (1 - D) = I_{\text{OUT}} \left(1 - \frac{V_{\text{OUT}}}{V_{\text{IN}}} \right) \quad (11)$$

8.2.2.5 Output Capacitor Selection (Buck Controllers)

The output capacitor is selected based on output voltage ripple and transient response requirements. As a result of the nature of the hysteretic control loop, a minimum ESR of a few tens of mΩ should be maintained for good operation unless a feed-forward resistor is used. Low ESR bulk tantalum or PosCap capacitors work best in most applications. A 1.0μF ceramic capacitor can be used in parallel with this capacitor to filter higher frequency spikes. The output voltage ripple can be estimated by [Equation 12](#):

$$\Delta V_{\text{PP}} = \Delta I \times \left[\text{ESR} + \left(\frac{1}{8 \times C_{\text{OUT}} \times f} \right) \right] \approx 1.1 \Delta I \times \text{ESR} \quad (12)$$

To calculate the capacitance needed to achieve a given voltage ripple as a result of a load transient from zero output to full current, use [Equation 13](#):

$$C_{\text{OUT}} = \frac{L \times \Delta I_{\text{OUT}}^2}{(V_{\text{IN}} - V_{\text{OUT}}) \times \Delta V} \quad (13)$$

If only ceramic or other very low ESR output capacitor configurations are desired, additional voltage ripple must be passed to the feedback pin. For detailed application information, refer to the [Using Ceramic Output Capacitors with the TPS6420x and TPS75003 Buck Controllers](#) application report.

8.2.2.6 Output Voltage Ripple Effect on V_{OUT} (Buck Controllers)

Output voltage ripple causes V_{OUT} to be higher or lower than the target value by half of the peak-to-peak voltage ripple. For minimum on-time, the ripple adds to the voltage; for minimum off-time, it subtracts from the voltage.

8.2.2.7 Soft-Start Capacitor Selection (Buck Controllers)

The soft-start for BUCK1 and BUCK2 is not intended to be a precision function. However, the startup time (from a positive transition on Enable to V_{OUT} reaching its final value) has a linear relationship to C_{SS} up to approximately 800pF, which results in a startup time of approximately 4ms. Above this value of C_{SS} , the variation in start-up time increases rapidly. This variation can occur from unit to unit and even between the two BUCK controllers in one device. Therefore, do not depend on the soft-start feature for sequencing multiple supplies if values of C_{SS} greater than 800pF are used.

BUCK1 is discussed in this section; it is identical to BUCK2. Soft-start is implemented on the buck controllers by ramping current limit from 0 to its target value (set by R_1) over a user-defined time. This time is set by the external soft-start cap connected to pin SS1. If SS1 is left open, a small on-chip capacitor will provide a current limit ramp time of approximately 250 μ s. [Figure 19](#) shows the effects of R_1 and SS1 on the current limit start-up ramp.

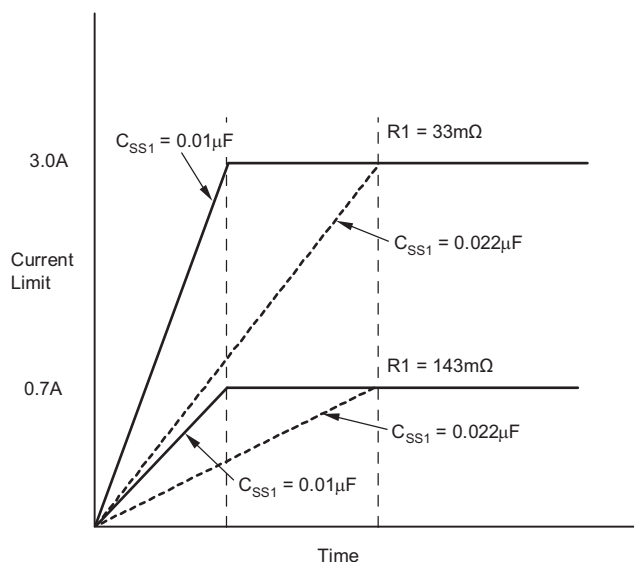


Figure 19. Effects of C_{SS1} and R_1 on Current Ramp Limit

This soft-start current limit ramp can be used to provide inrush current control or output voltage ramp control. While the current limit ramp can be easily understood by looking at [Figure 19](#), the output voltage ramp is a complex function of many variables. The dominant variables in this process are V_{OUT1} , C_{SS1} , I_{OUT1} , and R_1 . Less important variables are V_{IN1} and L_1 .

The best way to set a target start-up time is through bench measurement under target conditions, adjusting C_{SS1} to get the desired startup profile. To stay above a minimum start-up time, set the nominal start-up time to approximately five times the minimum. To stay below a maximum time, set the nominal start-up time at one-fifth of the maximum. Fastest start-up times occur at maximum V_{IN1} , with minimum V_{OUT1} , L_1 , C_{OUT1} , C_{SS1} , and I_{OUT1} . Slowest start-up times occur under opposite conditions.

Refer to [Figure 21](#) to [Figure 25](#) for characterization curves showing how the start-up profile is affected by these critical parameters.

8.2.2.8 Output Voltage Setting Selection (Buck Controllers)

Output voltage is set using two resistors as shown for Buck2 in [Figure 18](#). Output voltage is then calculated using [Equation 14](#):

$$V_{OUT} = V_{FB} \left(\frac{R5}{R6} + 1 \right)$$

where

- $V_{FB} = 1.22V$ (14)

8.2.2.9 Input Capacitor Selection (LDO)

Although an input capacitor is not required, it is good analog design practice to connect a 0.1μF to 10μF low ESR capacitor across the input supply near the regulator. This capacitor counteracts reactive input sources and improves transient response, stability, and ripple rejection. A higher value capacitor may be needed if large, fast rise-time load transients are anticipated, or if the device is located far from its power source.

8.2.2.10 Output Capacitor Selection (LDO)

A 2.2μF or greater capacitor is required near the output of the device to ensure stability. The LDO is stable with any capacitor type, including ceramic. If improved transient response or ripple rejection is required, larger and/or lower ESR output capacitors can be used.

8.2.2.11 Soft-Start Capacitor Selection (LDO)

The LDO uses an external soft-start capacitor, C_{SS3} , to provide an RC-ramped reference voltage to the control loop. See the [Functional Block Diagram](#). This is a voltage-controlled soft-start, as compared to the current-controlled soft-start used by the buck controllers. The start-up waveform can be approximated by [Equation 15](#):

$$V_{OUT}(t) = V_{OUT,SET} \left(1 - e^{-\frac{t}{RC}} \right)$$

where

- $R = 480 \times 10^3$
- C = capacitance in μF from SS3 to GND (15)

The time taken to reach 90% of final V_{OUT} can be approximated by [Equation 16](#):

$$T_{90\%} = 2.3 \times (480 \times 10^3) C_{SS3} (\mu F) \quad (16)$$

8.2.2.12 Setting Output Voltage (LDO)

Output voltage is set using two resistors as shown in [Figure 18](#). Output voltage is then calculated using [Equation 17](#):

$$V_{OUT} = V_{FB} \left(\frac{R3}{R4} + 1 \right)$$

where

- $V_{FB} = 0.507V$ (17)

8.2.3 Application Curves

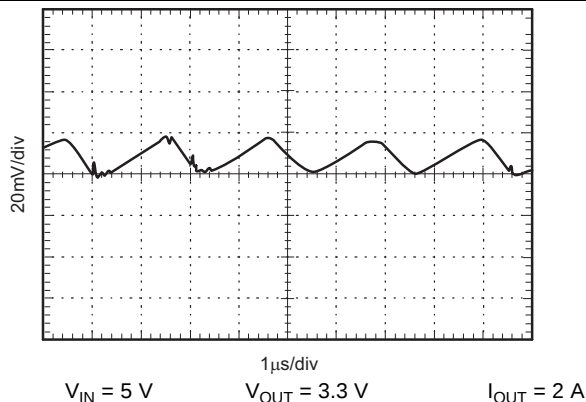


Figure 20. Buck Output Voltage Ripple

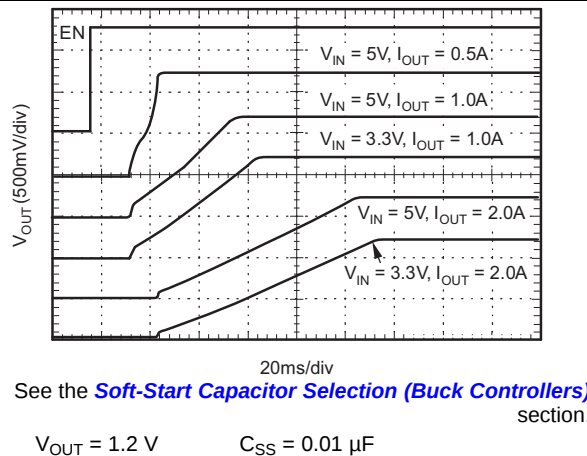


Figure 21. Buck Start-Up vs V_{IN} and I_{OUT}

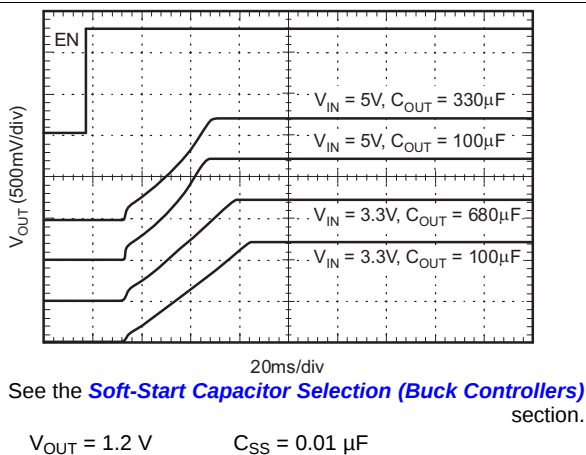


Figure 22. Buck Start-Up vs V_{IN} and C_{OUT}

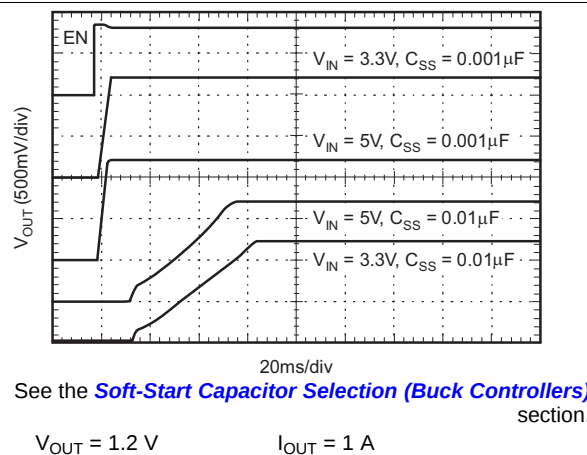


Figure 23. Buck Start-Up vs V_{IN} and C_{SS}

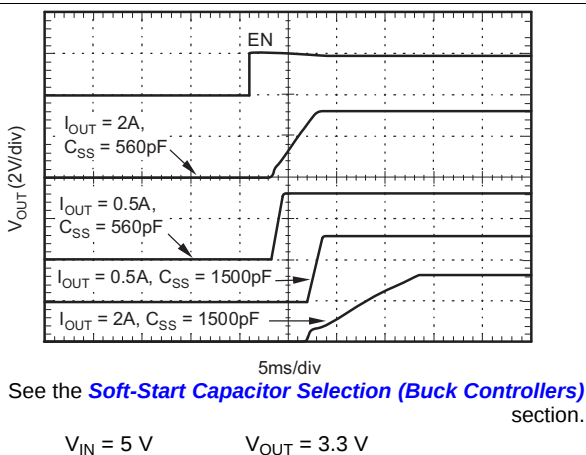


Figure 24. Buck Start-Up vs I_{OUT} and C_{SS}

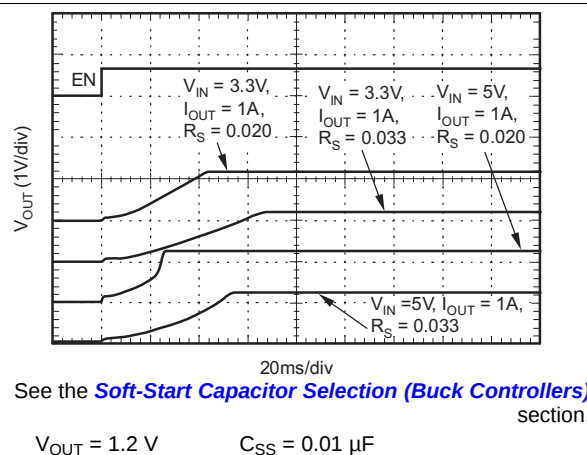


Figure 25. Buck Start-Up vs V_{IN} and R_{SENSE}

9 Power Supply Recommendations

There are three separate blocks internal to the TPS75003 device: two identical buck controllers and one integrated LDO regulator. The input voltage, V_{INX} , to the IN1 and IN2 pins must be within the range specified in the [Electrical Characteristics](#) and must be greater than the nominal output voltage of BUCK1 or BUCK2, respectively. However, the maximum output voltages, V_{OUT1} and V_{OUT2} , are determined by external component selection and cannot be specified. The input voltage to the LDO regulator, V_{IN3} , must be greater than the drop-out voltage (V_{DO}) added to V_{OUT3} or an absolute value of 2.2 V, whichever is greater. The power supply into the IN1, IN2, and IN3 pins do not need to be equal to each other but all of the design values must adhere to the minimum and maximum specifications of the TPS75003 and external components. Other considerations are based on the relationship of pins used inside the TPS75003 device.

The power supply into IN1 is used as the power supply to drive the gate of the switch connected at SW1. The difference between the voltages at the IN1 pin and IS1 pin is the input to the sensing which controls current limit. The power supply connected at IN1 must be the power supply connected to 33-m Ω sense resistor, and the opposite terminal of the sense resistor must connect directly to IS1 and the source pin(s) of the external PMOS FET.

Similarly, the power supply into IN2 is used as the power supply to drive the gate of the switch connected at SW2. The difference between the voltages at the IN2 pin and IS2 pin is the input to the sensing which controls current limit. The power supply connected at IN2 must be the power supply connected to 33-m Ω sense resistor, and the opposite terminal of the sense resistor must connect directly to IS2 and the source pins of the external PMOS FET.

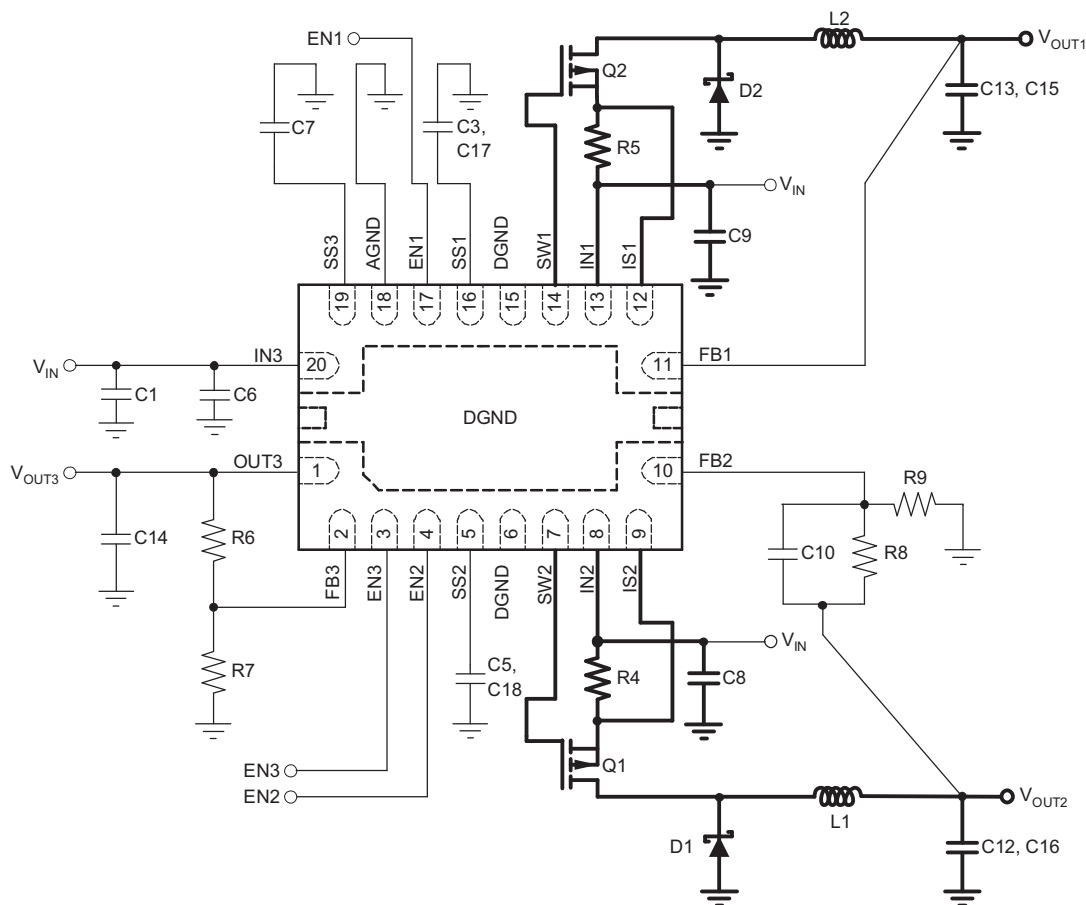
The power supply into IN3 is used as the power supply to the LDO regulator and all internal support circuitry. Unlike the BUCK1 and BUCK2 controllers, the power does not bypass the TPS75003 device. Therefore, the output of the LDO is named OUT3 and up to 300-mA of current will go directly from IN3 to OUT3.

10 Layout

10.1 Layout Guidelines

10.1.1 PCB Layout Considerations

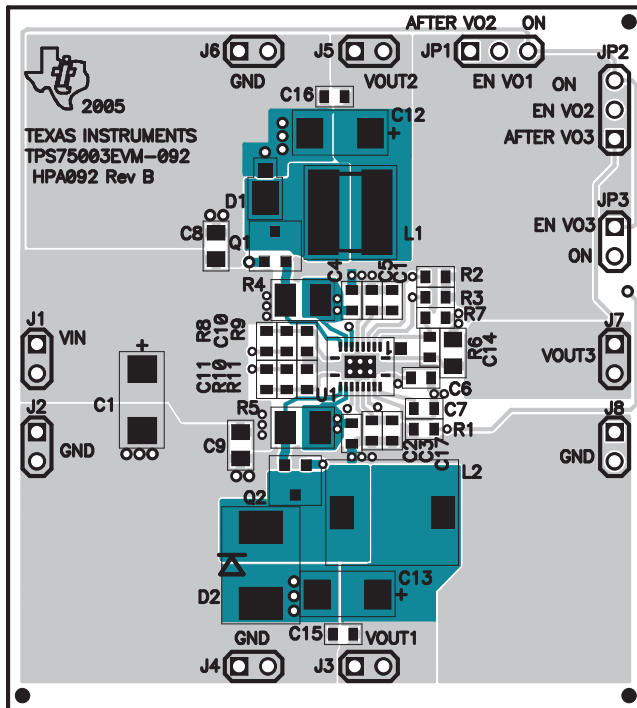
As with any switching regulators, careful attention must be paid to board layout. A typical application circuit and corresponding recommended printed circuit board (PCB) layout with emphasis on the most sensitive areas are shown in Figure 26 through Figure 28.



Note: Most sensitive areas are highlighted by bold lines.

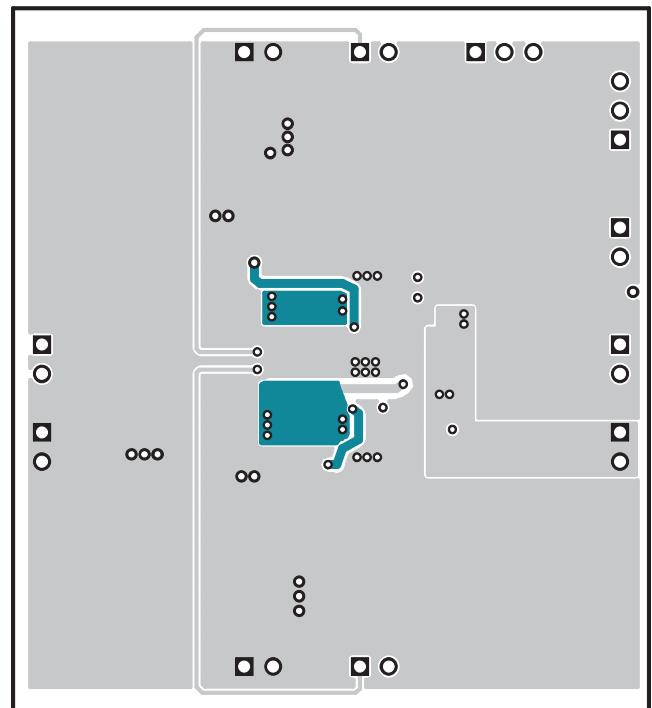
Figure 26. Typical Application Circuit

10.2 Layout Example



Most sensitive areas are highlighted in green.

Figure 27. Recommended PCB Layout, Component Side, Top View



Most sensitive areas are highlighted in green.

Figure 28. Recommended PCB Layout, Bottom Side, Top View

11 デバイスおよびドキュメントのサポート

11.1 デバイス・サポート

11.1.1 デベロッパー・ネットワークの製品に関する免責事項

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11.1.2 開発サポート

開発サポートについては、次の資料を参照してください。

- [TPS75003用のデザイン・スプレッドシート](#)
- [TPS75003: TPS75003用のGerberソフトウェア](#)

11.2 ドキュメントのサポート

11.2.1 関連資料

関連資料については、以下を参照してください。

- テキサス・インスツルメンツ、[『TPS75003EVMユーザー・ガイド』](#)
- テキサス・インスツルメンツ、[『Spartan-3の構成およびJTAGポートに対する3.3V信号の使用』アプリケーション・ノート](#)
- テキサス・インスツルメンツ、[『TPS6420xおよびTPS75003降圧コントローラでのセラミック出力コンデンサの使用』アプリケーション・レポート](#)

11.3 ドキュメントの更新通知を受け取る方法

ドキュメントの更新についての通知を受け取るには、[ti.com](#)のデバイス製品フォルダを開いてください。右上の「アラートを受け取る」をクリックして登録すると、変更されたすべての製品情報に関するダイジェストを毎週受け取れます。変更の詳細については、修正されたドキュメントに含まれている改訂履歴をご覧ください。

11.4 コミュニティ・リソース

The following links connect to TI community resources. Linked contents are provided "AS IS" by the respective contributors. They do not constitute TI specifications and do not necessarily reflect TI's views; see TI's [Terms of Use](#).

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設計サポート TIの設計サポート役に立つE2Eフォーラムや、設計サポート・ツールをすばやく見つけることができます。技術サポート用の連絡先情報も参照できます。

11.5 商標

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11.6 静電気放電に関する注意事項



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静電気放電はわずかな性能の低下から完全なデバイスの故障に至るまで、様々な損傷を与えます。高精度の集積回路は、損傷に対して敏感であり、極めてわずかなパラメータの変化により、デバイスに規定された仕様に適合しなくなる場合があります。

11.7 Glossary

[SLYZ022](#) — TI Glossary.

This glossary lists and explains terms, acronyms, and definitions.

12 メカニカル、パッケージ、および注文情報

以降のページには、メカニカル、パッケージ、および注文に関する情報が記載されています。この情報は、そのデバイスについて利用可能な最新のデータです。このデータは予告なく変更されることがあり、ドキュメントが改訂される場合もあります。本データシートのブラウザ版を使用されている場合は、画面左側の説明をご覧ください。

PACKAGING INFORMATION

Orderable part number	Status (1)	Material type (2)	Package Pins	Package qty Carrier	RoHS (3)	Lead finish/ Ball material (4)	MSL rating/ Peak reflow (5)	Op temp (°C)	Part marking (6)
TPS75003RHRLR	Active	Production	VQFN (RHL) 20	3000 LARGE T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 85	75003
TPS75003RHRLR.B	Active	Production	VQFN (RHL) 20	3000 LARGE T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 85	75003
TPS75003RHRLRG4	Active	Production	VQFN (RHL) 20	3000 LARGE T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 85	75003
TPS75003RHRLT	Active	Production	VQFN (RHL) 20	250 SMALL T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 85	75003
TPS75003RHRLT.B	Active	Production	VQFN (RHL) 20	250 SMALL T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 85	75003
TPS75003RHRLTG4	Active	Production	VQFN (RHL) 20	250 SMALL T&R	Yes	NIPDAU	Level-1-260C-UNLIM	-40 to 85	75003

⁽¹⁾ **Status:** For more details on status, see our [product life cycle](#).

⁽²⁾ **Material type:** When designated, preproduction parts are prototypes/experimental devices, and are not yet approved or released for full production. Testing and final process, including without limitation quality assurance, reliability performance testing, and/or process qualification, may not yet be complete, and this item is subject to further changes or possible discontinuation. If available for ordering, purchases will be subject to an additional waiver at checkout, and are intended for early internal evaluation purposes only. These items are sold without warranties of any kind.

⁽³⁾ **RoHS values:** Yes, No, RoHS Exempt. See the [TI RoHS Statement](#) for additional information and value definition.

⁽⁴⁾ **Lead finish/Ball material:** Parts may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

⁽⁵⁾ **MSL rating/Peak reflow:** The moisture sensitivity level ratings and peak solder (reflow) temperatures. In the event that a part has multiple moisture sensitivity ratings, only the lowest level per JEDEC standards is shown. Refer to the shipping label for the actual reflow temperature that will be used to mount the part to the printed circuit board.

⁽⁶⁾ **Part marking:** There may be an additional marking, which relates to the logo, the lot trace code information, or the environmental category of the part.

Multiple part markings will be inside parentheses. Only one part marking contained in parentheses and separated by a "~" will appear on a part. If a line is indented then it is a continuation of the previous line and the two combined represent the entire part marking for that device.

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OTHER QUALIFIED VERSIONS OF TPS75003 :

- Enhanced Product : [TPS75003-EP](#)

NOTE: Qualified Version Definitions:

- Enhanced Product - Supports Defense, Aerospace and Medical Applications

TAPE AND REEL INFORMATION



*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
TPS75003RH LR	VQFN	RHL	20	3000	330.0	12.4	3.8	4.8	1.6	8.0	12.0	Q1
TPS75003RH LT	VQFN	RHL	20	250	180.0	12.4	3.8	4.8	1.6	8.0	12.0	Q1

TAPE AND REEL BOX DIMENSIONS



*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
TPS75003RHRLR	VQFN	RHL	20	3000	356.0	356.0	35.0
TPS75003RHILT	VQFN	RHL	20	250	210.0	185.0	35.0

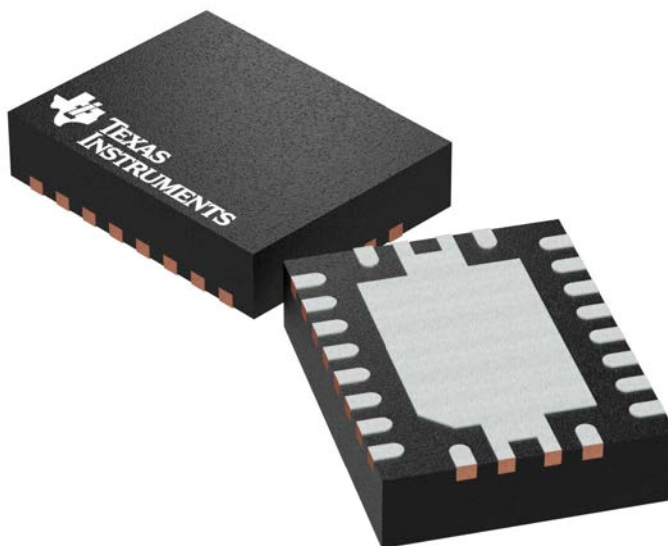
GENERIC PACKAGE VIEW

RHL 20

VQFN - 1 mm max height

3.5 x 4.5 mm, 0.5 mm pitch

PLASTIC QUAD FLATPACK - NO LEAD



Images above are just a representation of the package family, actual package may vary.
Refer to the product data sheet for package details.

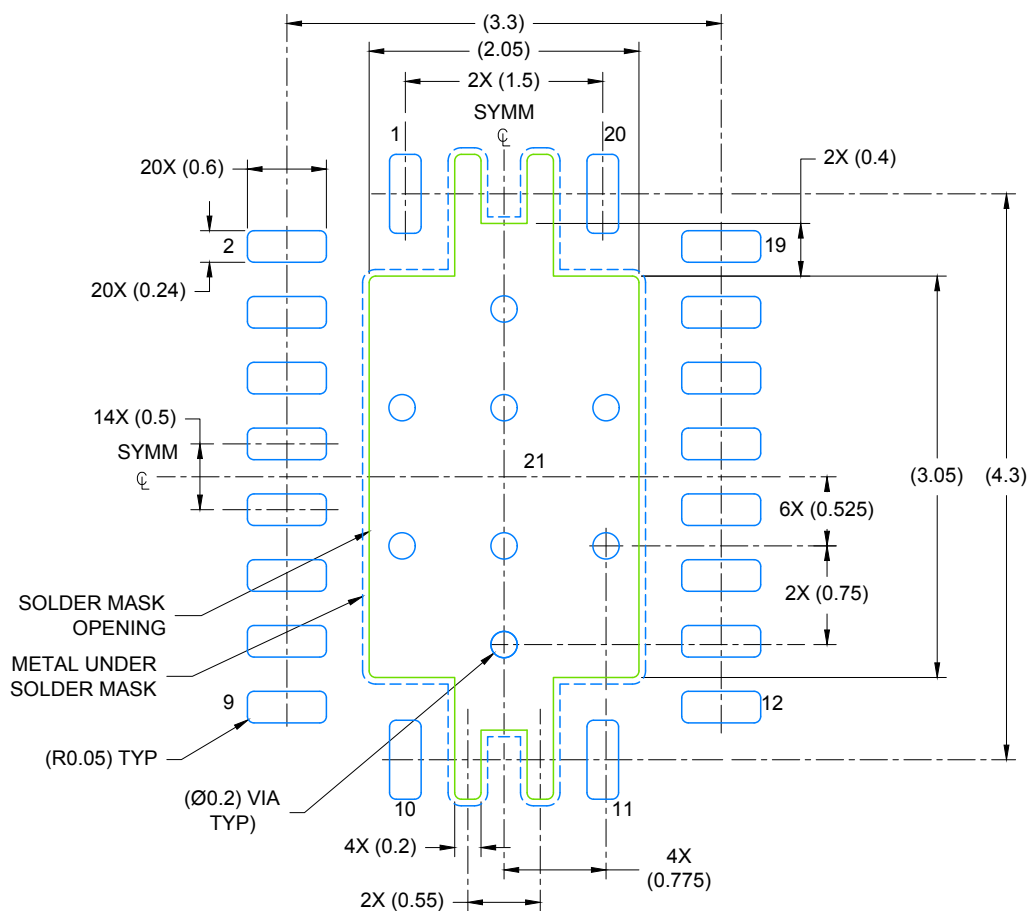
4205346/L

VQFN - 1 mm max height

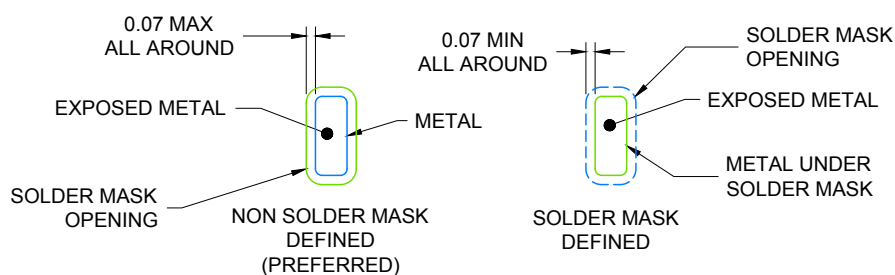
The drawing illustrates the mechanical specifications of a connector housing. The front view (top) shows a rectangular housing with a width of 3.6 (3.4) and a height of 4.6 (4.4). A shaded area on the left is designated as the 'PIN 1 INDEX AREA'. The side view (middle) shows a maximum height of 1 MAX and a seating plane with a 0.08 C tolerance. The detail view (bottom) shows a cross-section of the housing with various features and dimensions: 14X 0.5, 2X 3.5, 10, 11, 12, 19, 20, 21, 2X 1.5, 2.05±0.1, 20X 0.5/0.3, 20X 0.29/0.19, 4X (0.2), 2X (0.55), 0.1 (M) C A B, 0.05 (M) C, and (0.2) TYP. The drawing also includes a 'PIN 1 ID (OPTIONAL)' callout and a 'SEATING PLANE' label.

NOTES:

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. The package thermal pad must be soldered to the printed circuit board for thermal and mechanical performance.



LAND PATTERN EXAMPLE
EXPOSED METAL SHOWN
SCALE: 18X

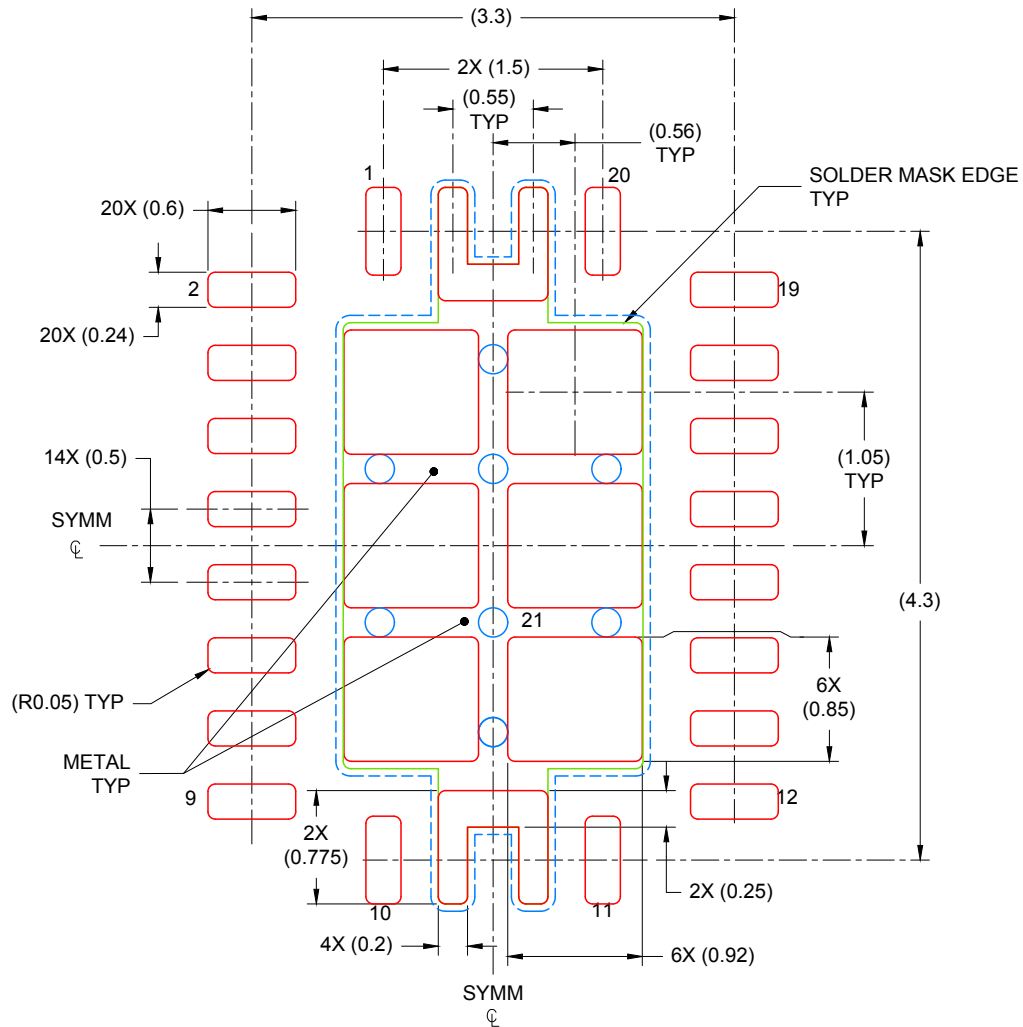


SOLDER MASK DETAILS

4219071 / A 05/2017

NOTES: (continued)

4. This package is designed to be soldered to a thermal pad on the board. For more information, see Texas Instruments literature number SLUA271 (www.ti.com/lit/sluea271).
5. Solder mask tolerances between and around signal pads can vary based on board fabrication site.
6. Vias are optional depending on application, refer to device data sheet. If any vias are implemented, refer to their locations shown on this view. It is recommended that vias under paste be filled, plugged or tented.



SOLDER PASTE EXAMPLE
 BASED ON 0.1mm THICK STENCIL

EXPOSED PAD
 75% PRINTED COVERAGE BY AREA
 SCALE: 20X

4219071 / A 05/2017

NOTES: (continued)

7. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations..

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